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CPW Fed Rectangular

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Highlights

Planar CPW Antenna Loaded

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VOLUME 16 ISSUE 2 VERSION 1.0



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CPW Fed Rectangular Microstrip Patch Antenna with Upper Pentagonal End Cut

By Paresh Jain & Prof. (Dr.) R.K Khola

Suresh Gyan Vihar University, India

Abstract- In this paper we have designed a CPW fed rectangular microstrip patch antenna at resonant frequency of 2.4 GHz. These types of microstrip antennas give high performance, robust in design and easy to fabricate. Patch elements are placed on FR-4 epoxy substrate of relative permittivity 4.4 kept at a substrate height of 1.6 mm. Simulation results are presented using HFSS version 13.0. The return loss obtained is $-22db$, and the impedance bandwidth achieved is 37%, VSWR is 1.15 and the gain is $2.55db$ at the centre frequency of 2.4 GHz.

Keywords: *microstrip antenna, CPW fed, hfss 13.0, 2.4 GHz and FR-4 epoxy.*

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Keywords: microstrip antenna, CPW fed, hfss 13.0, 2.4 GHz and FR-4 epoxy.

I. INTRODUCTION

In the early 1970's the first practical microstrip antenna was fabricated by Howel & Munson and These above said antennas became popular during the 70's period as this antennas had the space borne applications. Antennas play a vital role in communication systems to transmit and receive signals. Microstrip antennas are versatile in geometrical dimensions and can be implemented easily. They are useful as they are of low profile, low power handling, low weight, simple and cheap [1]. Due to their attractive features like high rate of transfer of data and compact size have increased their demand and various applications immensely. The Microstrip antennas are of very high performance, robust in design and easy to fabricate [2].

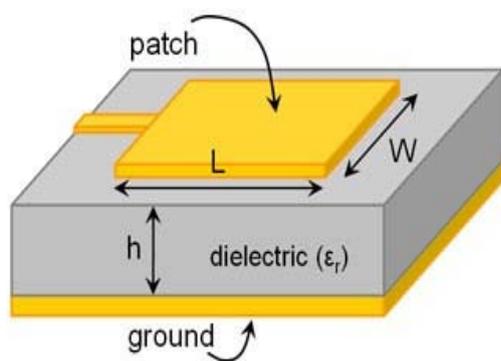


Figure 1 : Block of Schematic of Microstrip Antenna

Many problems such as the surface wave excitation and narrow bandwidth are overcome by

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various methods such as cutting slot, increasing thickness, etc. CPW is used in designing antenna which has low weight and low transmission losses and this method was introduced by C.P. Wen in 1969 [3]. CPW-Feed method is cheap and the line impedance and phase velocity are less dependent on substrate height than on slot width [4]. The design geometry and the results of the proposed antenna are presented in this paper.

II. ANTENNA DESIGN

The design is based on transmission line model analysis and it has rectangular patch antenna with upper pentagonal end cut in a circular slot on the ground. The geometry of this antenna is shown in figure 2. In the designing of this antenna three basic parameters are required to be decided, such as thickness of substrate, relative permittivity and dielectric substrate. Thickness of substrate reduces the size of antenna and surface radiations and low dielectric constant is preferred because the antenna gives better efficiency, low losses and higher bandwidth, thus the patch elements are placed on FR-4 epoxy substrate of relative permittivity 4.4 kept at 1.6 mm. height. Feed line width is such that impedance is 50_ [5]. The antenna is designed with a centre frequency of 2.4GHz. The dimensions of the proposed antenna are shown in Table 1.

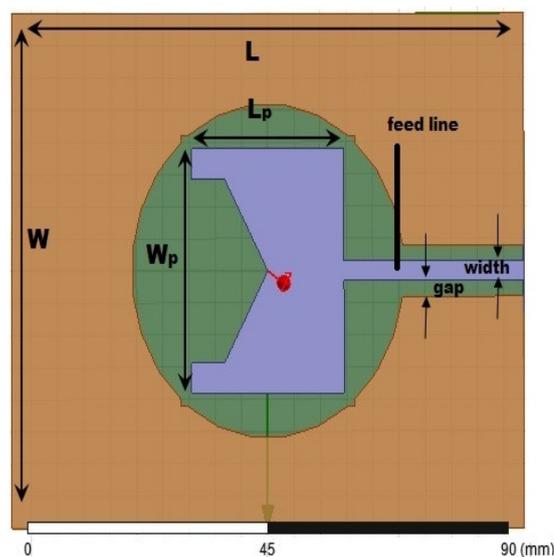


Figure 2 : Geometry of the proposed antenna

Table 1 : The dimensions of the proposed antenna.

Parameter	Value
Length of patch (L_p)	29mm
Width of patch (W_p)	38mm
Length of substrate (L)	97.48mm
Width of substrate (W)	80mm
Length of feed line	34.24mm
Width of feed line	3.045mm
Height of substrate	1.6mm
Radius of circle	26mm

III. RESULTS

Simulated results are obtained by using Ansoft HFSS 13.0 software. The results are presented and discussed in the following para.

a) Return Loss

The characteristics and measurement of the parameter return loss shows that how the antenna is effective in delivering the power from the source to the antenna. Return loss found is -22.1 dB . The graph of return loss versus frequency is shown in figure 3.

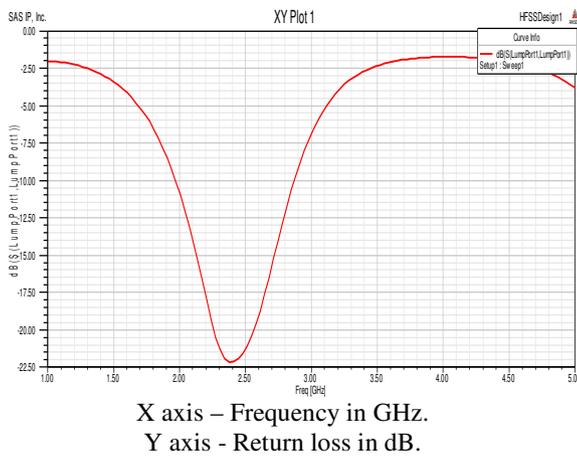


Figure 3 : Return Loss

b) Bandwidth

Return loss graph can be used in calculating the bandwidth of the antenna. The proposed antenna gives the 10 dB impedance bandwidth of 37%. The antenna can operate in the frequency range from 1.97GHz to 2.87 GHz.

c) Radiation Pattern

The radiation pattern shows the direction in which the power is directed and is also shows the radiation distribution and the power distribution in the particular direction. The figure 4 shows the 3-D radiation pattern of the said antenna at centre frequency 2.4 GHz.

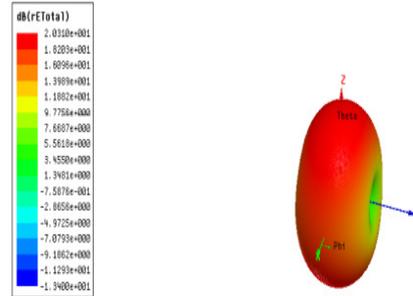


Figure 4 : Radiation Pattern.

d) VSWR

The voltage standing wave ratio is the ratio of the maximum and the minimum voltages at the feed line. The value of the VSWR which is determined for perfect matching of the antenna is such that it should be less than 2. The value should be 1:1 for maximum power transfer and for the antenna to perform efficiently. The plot of VSWR observed at the frequency 2.4 GHz. is 1.15 shown in figure 5.

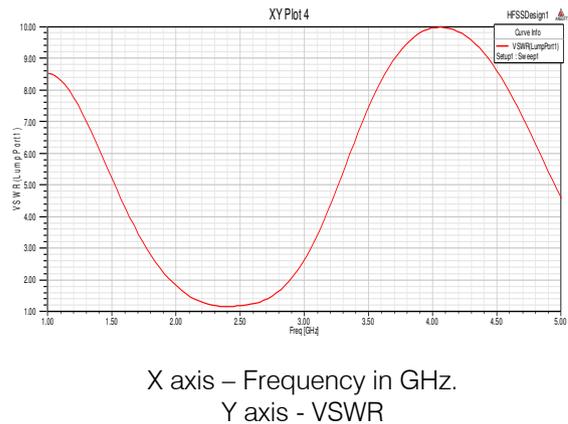


Figure 5 : VSWR

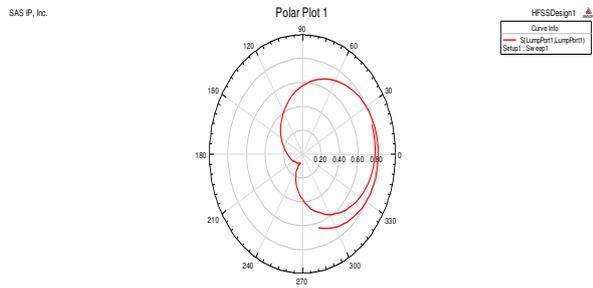


Figure 6 : Smith Chart

The smith chart in figure 6 shows VSWR of 1.15 at an angle of 109.23 and magnitude 0.0702 and impedance is 0.9466-0.1261i which indicates that the antenna is resistive in nature.

e) Gain

The parameter gain shows the amount of the power transmitted in the maximum radiation direction where the isotropic source is taken. The gain should not be less than 0 dB otherwise the antenna is not radiating. The gain of the proposed antenna measured to be 2.55 dB and shown in figure 7.



Figure 7 : Gain

IV. CONCLUSION

The proposed antenna is based on CPW-Fed technique and from the simulated result, gain is observed as 2.55 and the return loss calculated is -22.1, The VSWR value calculated is 1.17 and the impedance bandwidth calculated is 37% for the proposed antenna. Simulation and design of the microstrip patch antenna is done on a substrate of dielectric constant 4.4 and at a resonant frequency of 2.4GHz which ranges from 1.97GHz to 2.87GHz and successfully done using HFSS Software. Several other designs can be simulated using different parameters having better results and higher efficiency for applications in the field of wireless communication. Their main applications may be in extended UTMS, Wi-Fi, WiMax, etc.

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Control Strategies of a Neuro-Fuzzy Controlled Grid Connected Hybrid PV/PEMFC/Battery

By T. Praveen Kumar, N. Subrahmanyam & M. Sydulu

National Institute of Technology, India

Abstract- This paper depicts power control strategies of a neuro-fuzzy controlled grid connected hybrid photovoltaic and proton exchange membrane fuel cell distributed generation system with battery as energy storage device. The essential source of energy for the hybrid distributed generation system is from photovoltaic cell and proton exchange membrane fuel cell and the battery acts as a complementary source of energy. The hybrid distributed generation system is connected to a grid through power electronic interfacing devices. A Matlab/Simulink model is developed for the grid connected hybrid distributed generation system, neuro-fuzzy controlled power electronic DC/DC and DC/AC converters to control the flow of power on both sides. Likewise we extended our work so as to distribute the power between power sources, the neuro-fuzzy power controller has been developed. Simulation results are presented to demonstrate the effectiveness and capability of proposed control strategy.

Keywords: *shunt active power filters, total harmonic distortion, power conversion, power drives.*

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I. INTRODUCTION

The penetration level of green and renewable energy sources/distributed generation units are expected to grow in the near future as there is a probability of rundown conventional fuels for power generation. The distributed generation is classified as renewable and non-renewable. The distributed generation sources such as Fuel cells, Wind and Solar energy are increasing daily due to increase in demand for electrical power [1]. These energy sources are environmental friendly, reduces transmission and distribution losses, peak load shaving, can be used as backup sources and etc. Fuel cell is a promising device as it is efficient, modular and can be placed at any site for improving system efficiency [2] but it has slow start-up response. Solar energy is an important renewable energy source [3] but the intermittent nature of this technology is a major issue. The accessibility of energy is driven by climate and cell temperature however not on the loads of the systems. This innovation can be marked as irregular and typically PV array utilizes a Maximum Power Point Tracking (MPPT) (MPPT) strategy to consistently convey the most highest power to the load when there are variations in irradiation and temperature [4]. Because of the intermittent nature of PV array it

becomes an uncontrollable source. In order to overcome the drawbacks with the slow start-up of fuel cells and intermittent nature of PV cell a neuro-fuzzy controlled grid associated hybrid photovoltaic as well as proton exchange membrane fuel cell (PEMFC) distributed generation system with battery as energy storage is suggested in this paper.

II. SYSTEM MODELING

Fig. 1 shows the block diagram of the HRPS (Hybrid Renewable Power Sources) proposed in this paper that connected to main grid in Point Common Coupling (PCC). So by above discussions two mathematical models recitation the dynamic behavior and each of these constituents are given below.

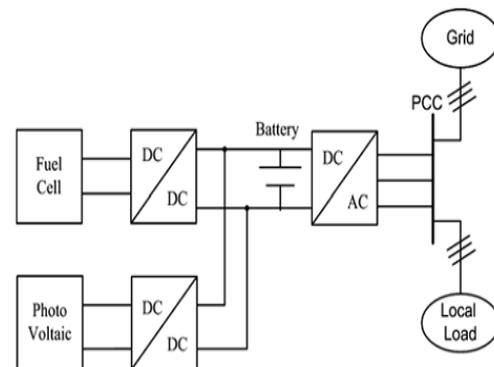


Fig-1 : Block Diagram of Grid connected Hybrid system

a) Proton Exchange Membrane Fuel Cell Model

A fuel cell functions like a battery by transforming the chemical energy into electrical energy, but it differs from a battery in that as long as the hydrogen and oxygen is supplied it will produce DC electricity continuously. Fuel cells play a vital role in distributed generation because of their advantages such as high efficiency, no contamination gasses and particular structure adaptability.

The Nernst's mathematical statement and Ohm's law oversee the normal voltage size of the fuel cell stack. The subsequent mathematical statement representations the voltage of the fuel cell stack:

$$V_{fc} = N_0(E_0 + \frac{RT}{2F} (\log \left(\frac{P_{H_2} P_{O_2}^{0.5}}{P_{H_2O}} \right))) - R_{int} I \quad (1)$$

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Where:

N_0 is the number of cells connected in series;
 R_{int} is the internal resistance of fuel cell stack [Ω]
 E_0 is the voltage related with the reaction free energy;
 R is the universal gas constant;
 T is the temperature;
 I is the current of the fuel cell stack;
 F is the Faraday's constant.

$P_{H_2}, P_{H_2O}, P_{O_2}$ are dictated by the accompanying differential equations.

$$\begin{aligned}
 P_{H_2} &= -\frac{1}{t_{H_2}}(P_{H_2} + \frac{1}{K_{H_2}}(q_{H_2}^{in} - 2K_r I_{fc})) \\
 P_{H_2O} &= -\frac{1}{t_{H_2O}}(P_{H_2O} + \frac{2}{K_{H_2O}}K_r I_{fc}) \\
 P_{O_2} &= -\frac{1}{t_{O_2}}(P_{O_2} + \frac{1}{K_{O_2}}(q_{O_2}^{in} - K_r I_{fc}))
 \end{aligned}
 \tag{2}$$

Where, $q_{H_2}^{in}$ and $q_{O_2}^{in}$ are the molar flow of hydrogen and oxygen and where the K_r constant is well-defined by the relation between the rate of reactant hydrogen and the fuel cell current:

$$q_{H_2}^r = \frac{N_0 I}{2F} = 2K_r I \tag{3}$$

Besides, a straightforward model of reformer that creates hydrogen through methane has been deliberated and the model is second-order transfer function. So therefore its mathematical form can be written as follows:

$$\frac{q_{H_2}}{q_{metanne}} = \frac{CV}{\tau_1 \tau_2 S^2 + (\tau_1 + \tau_2)S + 1}$$

Where $q_{metanne}$ is methane flow rate [kmol/sec];
 CV is conversion factor [kmol of hydrogen per kmol of methane];

τ_1, τ_2 are reformer time constants [sec].

b) Photovoltaic Model (PV)

The equivalent circuit shown in Fig.2 is a one diode model of a solar cell which consists of a diode and a current source connected in parallel with a series resistance R_s . The current source feeds the photocurrent I_{ph} , which is directly proportional to solar irradiance G . By referring manufacturer's data sheet, the two main parameters used to describe a PV cell are open circuit voltage and another is its short circuit current.

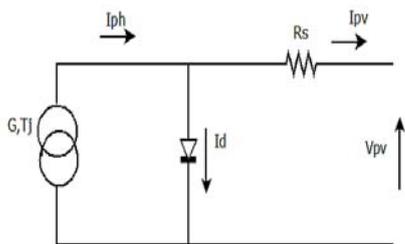


Fig.2 : Equivalent solar cell model with R_s

The mathematical model [3] of PV cell can be expressed as

$$I_{pv} = I_{ph} - I_0 \left[\exp q \left(\frac{V_{pv} + I_{pv} \cdot R_s}{AKT} \right) - 1 \right] \tag{4}$$

Since Photocurrent I_{ph} is directly proportional to solar radiation G .

$$I_{ph}(G) = I_{sc} \frac{G}{G_{ref}} \tag{5}$$

The short-circuit current I_{sc} of solar cell depends linearly on cell temperature.

$$I_{sc}(T_j) = I_{sc} [1 + \Delta I_{sc} (T_j - T_{jref})]$$

$$I_{ph}(G, T_j) = I_{scs} \frac{G}{G_{ref}} [1 + \Delta I_{sc} (T_j - T_{jref})] \tag{6}$$

I_0 also depends on solar irradiation as well as cell temperature and that can be mathematically expressed as follows

$$I_0(G, T_j) = \frac{I_{ph}(G, T_j)}{e \left(\frac{V_{oc}(T_j)}{V_t(T_j)} \right) - 1} \tag{7}$$

In the writing numerous MPPT strategies are accessible, for instance, incremental conductance (INC), consistent voltage (CV), and perturbation and observation (P&O). Therefore P&O strategy has been generally utilized in view of its basic input structure and less measured parameters. The panel voltage is purposely intentionally agitated (expanded or diminished) then the power is contrasted with the power got before to disturbance. In particular, if the power panel is increased because of the unsettling influence, the accompanying disturbance will be made in the same course and if the power diminishes, the new perturbation is made in the opposite direction. But the demerit with P & O is the output power is oscillating in nature. Because of this reason we use the Fuzzy MPPT technique to deliver the maximum power and to eliminate perturbations in the output power.

c) Fuzzy MPPT Control

The inputs to the fuzzy MPPT control can be measured or computed from the voltage and current of solar panel. The control rules are indicated in [4] with ΔP_{pv} and ΔV_{pv} as inputs and ΔV_{pvref} as the output. The membership functions of input and output variables in which membership functions of input variables ΔP_{pv} and ΔV_{pv} are triangular and has seven fuzzy subsets. Seven fuzzy subsets are considered for membership functions of the output variable ΔV_{pvref} . These input and output variables are expressed in terms of linguistic variables (such as BN (big negative), MN (Medium negative), SN (small negative), Z (zero), SP (small positive), MP (medium positive), and BP (big positive)).

d) Battery Modelling

The battery is a device which stores energy in electro chemical form. Battery is used as energy storage device in wide range of applications like hybrid electric vehicles and hybrid power systems. In this paper, the battery energy storage is combined with hybrid PV/PEMFC distributed generation system. The battery model considered in this paper is shown in fig.3. The battery model used is based on voltage model proposed by Shepherd [4].

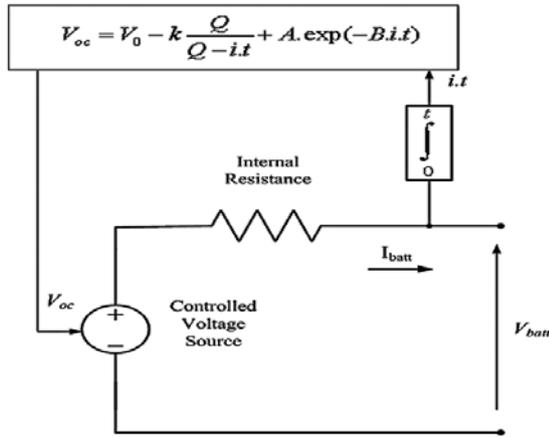


Fig. 3 : Battery Model

e) DC/DC Boost Converter Model

The role of boost DC/DC converters is to deliver power to the user in appropriate form at high efficiency. Generally the Power electronic converters are desirable in PV and fuel cell systems to transform DC voltage to the prerequisite values. Fig. 4 shows the DC/DC converter model.

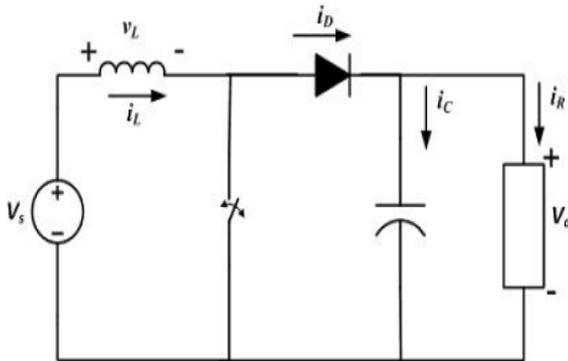


Fig. 4 : Boost DC/DC Converter Model.

As depicted above boost converter is defined by the following two nonlinear state space averaged equations [7]:

$$\begin{aligned} \frac{di_L}{dt} &= -\frac{R_L}{L} - \left(\frac{1-d}{L}\right)V_0 + \frac{1}{L}V_s \\ \frac{dV_C}{dt} &= \left(\frac{1-d}{C}\right)i_L + \frac{i_R}{C} \end{aligned} \quad (8)$$

where “d” is the duty cycle of the switching device, “U” is the input voltage, “i_L” is the inductor

current, “V_c” is the output voltage and “i_o” is the output current.

f) DC-AC Converter Model

Converter (VSC) is shown in Fig. 5. To reduce harmonics, LCL filter is connected between the converter and also at the grid side [6]. So therefore the dynamic model of the three-phase VSC is represented in

$$\begin{aligned} \frac{di_{1k}}{dt} &= -\frac{R_1}{L_1}i_{1k} + \frac{1}{L_1}(V_{1k} - V_{ck}) \\ \frac{di_{2k}}{dt} &= -\frac{R_2}{L_2}i_{2k} + \frac{1}{L_1}(V_{ck} - V_{sk}) \\ C_f \frac{dV_{ck}}{dt} &= i_{1k} - i_{2k} \end{aligned} \quad (9)$$

Where k={a, b, c}

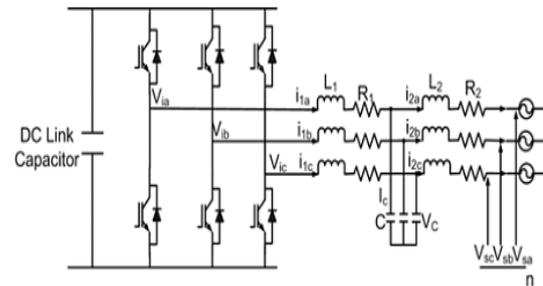


Fig.5 : DC/ AC Three Phase Inverter

III. POWER CONTROL STRATEGIES OF HYBRID SYSTEM

By above discussions the Power flow control from hybrid power sources to local AC bus and to/from storage devices is required to keep up power balance at all times while fulfilling the the active and reactive power demanded by the load. Eq.(13) gives power balance expressions that should be satisfied together at the DC-link and at the P_{CC} all the time.

The rate and magnitude of fuel cell power P_{FC} and rate, sign and magnitude of battery power P_{Batt} depend on the magnitude and how fast the load changes.

$$\begin{aligned} P_{DG} &= P_{PV} + P_{PC} + P_{Batt} \\ P_{Load} &= P_{DG} + P_{Grid} \\ Q_{Load} &= Q_{DG} + Q_{Grid} \end{aligned} \quad (10)$$

According to the control strategy proposed in this paper, P_{Load} and Q_{Load} are made equal to P_{ref} and Q_{ref} so that the hybrid power system output shadows the load demand only under normal loading conditions also P_{Grid} and Q_{Grid} are seems to be zero. So if the local load demand surpasses the hybrid power system capacity, then remaining of the power is supplied from the grid side. Fig. 6 shows the overall structure of the control strategy.

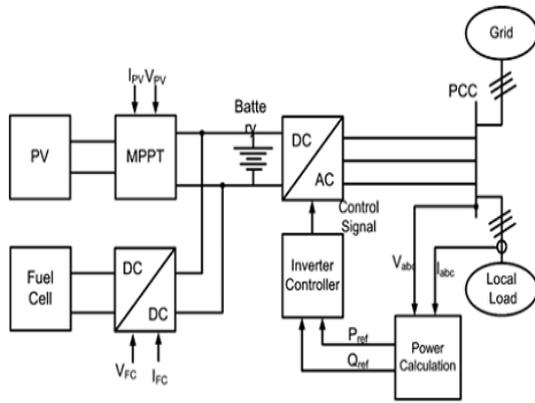


Fig. 6 : Overall system control structure.

Hence the control strategy also retains the DC-link/battery voltage within a band about the nominal DC-link voltage to have the inverter in synchronism with the grid. The following differential equation for DC link power balance is given:

$$C_{dc} v_{dc} \frac{dv_{dc}}{dt} = P_{FC} + P_{PV} + P_{Batt} - P_{Grid} \quad (11)$$

Moreover, to meet the requirements of power balance in DC link it is significant to consider the dynamic limitations of fuel cell power. In this case, the fuel cell power could not change rapidly and the fuel cell controller with DCDC converter should regulate the operating point of fuel cell. But the amount of power that should be absorbed by battery energy storage in order to balance the power in DC link is significant and also it is greatly influenced by DC link energy, where its energy measurement is supported with the help of the following calculation:

$$E_{dc}(k) = \left(\frac{1}{2}\right) C_{dc} V_{dc}^2(k) \quad (12)$$

In this paper, a power flow control structure has been established for hybrid power sources during voltage sag. It is based on Fuzzy Logic Control (FLC) strategy that determines the battery energy storage power according to the following inputs:

$$e(k) = E_{dc-ref}(k) - E_{dc}(k) \quad (13)$$

$$\Delta e(k) = e(k) - e(k-1)$$

where E_{dc-ref} is the reference dc link energy which is calculated by reference dc link voltage. Subsequently, it is crucial to outline powerful and stable control technique to ensure the stability of the dc link of hybrid system. For this purpose, a fuzzy neural control strategy is developed [8].

IV. NEURO-FUZZY CONTROL STRATEGY

In this paper a neuro-fuzzy control strategy, for each of the input, four fuzzy subsets have been employed. These are ZE (zero), L (low), M (medium) and H (high). So for all of these fuzzy sets, a gaussian membership function has been used. As each of the two

inputs has four subsets, there are altogether 16 control rules in the neuro-fuzzy logic controller.

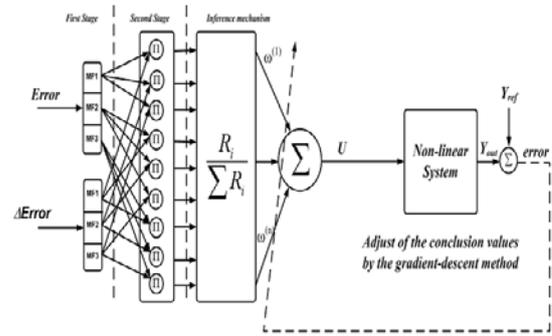


Fig.7 : The neuro-fuzzy scheme

The neuro-fuzzy calculation utilizes membership functions of gaussian kind. With Gaussian fuzzy sets, the algorithm is fit for using all data contained in the preparation set to calculate each rule conclusion, which is distinctive when utilizing triangular allotments. Fig.7 represents the neuro-fuzzy scheme for an illustration with two variables (x_1, x_2) and one output variable (y). In the principal phase of the neuro-fuzzy scheme, the two inputs are categorized into philological values by the set of Gaussian membership functions recognized to every variable. The second stage computes every tenet $R^{(0)}$ its separate enactment degree. Last, the derivation system weights every guideline conclusion $\omega^{(0)}$, instated by the group based algorithm, utilizing the enactment degree computed in the second stage. As mentioned the error signal among the model inferred value Y and the particular measured value (or teaching value) y' , is employed by the gradient descent scheme to regulate each rule conclusion. Also he algorithm adjusts the values of $\omega^{(0)}$ to diminish an objective function E typically expressed by the mean quadratic error (12). In this equation, the value $y'(k)$ is the preferred output value correlated with the condition vector $x'(k) = (x_1', x_2', \dots, x_m')$. The element $Y(x'(k))$ is the conditional response to the same condition vector $x'(k)$ and calculated by Eq. (14).

$$E = \frac{1}{2} [Y(x(k)) - y(k)]^2$$

$$Y(x'(k)) = \frac{\sum_{l=1}^c \left(\prod_{j=1}^m \mu_{A_j^{(l)}}(x_j'(k)) \right) \omega^{(l)}(k)}{\sum_{l=1}^c \left(\prod_{j=1}^m \mu_{A_j^{(l)}}(x_j'(k)) \right)} \quad (14)$$

Eq. (15) establishes adjustment for every conclusion $\omega^{(0)}$ with the aid of gradient-descent method. Here the symbol α is the learning rate parameter, and also t designates the number of learning iterations that are executed by the algorithm.

$$\omega^{(l)}(t+1) = \omega^{(l)}(t) - \alpha \frac{\partial E}{\partial \omega^{(l)}} \quad (15)$$

The inference function Eq. (14) depends on $\omega^{(l)}$ only through its numerator. The expression composing the numerator is now represented by 'a' and is shown in Eq.(16).

$$a = \sum_{l=1}^c \left(\prod_{j=1}^m \mu_{A_j^{(l)}}(x'_j(k)) \right) \omega^{(l)}(k) \quad (16)$$

The denominator of function Eq. (14) is dependent on a term $d^{(l)}$, defined in Eq. (17), and denoted by b in Eq. (18).

$$d^{(l)} = \prod_{j=1}^m \mu_{A_j^{(l)}}(x'_j(k)) \quad (17)$$

$$b = \sum_{l=1}^c (d^{(l)}) \quad (18)$$

In order to compute the adjustment of each conclusion value $\omega^{(l)}$, it is necessary to compute the variation of the objective function E, ∂E , in relative to the disparity that occurred in $\omega^{(l)}$ in the anterior instant, $\partial \omega^{(l)}$. So by, using the chain rule to calculate $\partial E / \partial \omega^{(l)}$ results in Eq.(19).

$$\frac{\partial E}{\partial \omega^{(l)}} = \frac{\partial E \partial Y}{\partial Y \partial a} \frac{\partial a}{\partial \omega^{(l)}} \quad (19)$$

The utilization of chain rule searches for the term contained in E that is straight forwardly reliant on the quality to be balanced, i.e., the conclusion value $\omega^{(l)}$. Therefore, we can verify by chain Eq. (19) that it starts with E dependent of Y value, and it basically depends on α term also finally, expression a is a function of $\omega^{(l)}$. Now after few moment, the alteration can be done for $\omega^{(l)}$ and also be interpreted that is propotional to the error that is between the neuro-fuzzy model response and the supervising value, but it can be weighted by the influence of rule (1), indicated by $d^{(l)}$, to the final neuro-fuzzy inference.

$$\omega^{l}(t + 1) = \omega^{(l)}(t) - \alpha \frac{(Y(x'(k)-y'(k))d^{(l)})}{\sum_{l=1}^c (d^{(l)})} \quad (20)$$

Next, a convergence theorem has been developed to assurance the stability of particular learning algorithm employed for the above-mentioned FNN [10]. A Lyapanov energy function is defined as follows:

$$V_k = J_k = \frac{1}{2} E_k^2 \quad (21)$$

From Eq. (19), we can get

$$\Delta V = V_{k+1} - V_k = \frac{1}{2} (E_{k+1}^2 - E_k^2) \quad (22)$$

The error difference, ΔE_k , can be defined as

$$\Delta E_k = E_{k+1} - E_k = \frac{\partial E_k}{\partial \omega} \Delta \omega \quad (23)$$

$$\Delta \omega = \omega_{k+1} - \omega_k = -\alpha E_k \frac{\partial E_k}{\partial \omega} \quad (24)$$

Using Eq. (22), we can get

$$\begin{aligned} \Delta V &= \frac{1}{2} (E_{k+1} - E_k)(E_{k+1} + E_k) \\ &= \frac{1}{2} (\Delta E_k)(2E_k + \Delta E_k) \end{aligned} \quad (25)$$

Substituting eq. (24) into eq. (23), we have:

$$\begin{aligned} \Delta V &= \frac{1}{2} \frac{\partial E_k}{\partial \omega} \alpha E_k \frac{\partial E_k}{\partial \omega} (-2E_k + \frac{\partial E_k}{\partial \omega} \alpha E_k \frac{\partial E_k}{\partial \omega}) \\ &= \frac{1}{2} (E_k \frac{\partial E_k}{\partial \omega})^2 [(\frac{\partial E_k}{\partial \omega})^2 \alpha^2 - 2\alpha] \end{aligned} \quad (26)$$

If $\Delta V < 0$, the convergence of the algorithm described in eq.(26) can be guaranteed. Therefore, we have:

$$(\frac{\partial E_k}{\partial \omega})^2 \alpha^2 - 2\alpha < 0 \quad (27)$$

From eq. (27), we can obtain:

$$0 < \alpha < \frac{2}{(\frac{\partial E_k}{\partial \omega})^2} \quad (28)$$

V. SIMULATION RESULTS

To evaluate the viability of the proposed control strategy, the system is simulated in SIMULINK/SIMPOWER for a period of 100sec of real and reactive load profiles.

Table 1: Hybrid distributed generation system parameters.

PEMFC Parameters	Values
Faraday's Constant	96487000 C/kmol
Hydrogen time constant(t_{H_2})	26.1 sec
Hydrogen valve molar constant(K_{H_2})	8.43×10^{-4}
Kr Constant= $N_0/4F$	9.9497×10^{-7}
No load voltage (E_0)	0.6V
Number of cells (N_0)	384
Oxygen time constant (t_{O_2})	2.91 sec
Battery Model parameters	Values
Maximum allowable terminal voltage	730 V
Minimum allowable terminal voltage	710 V
Operating Terminal Voltage	725 V

SOC, %	70
DC/AC Converter Parameters	
Nominal AC Voltage	400 V
Nominal Phase Current	125 A
Nominal DC Voltage	720 V
R _s	0.9 mΩ
L _s	0.01mH
F _s (Hz)	50 Hz
DC/DC Converter Parameters	
Rated Voltage (V)	200/650V
Resistance (R)	2.3Ω
Rated Power	50KW
Capacitance (C)	1.5 mf
Inductor (L)	415 μH

The decision of the DC- bus voltage depends on the output voltage of the inverter required which must provide the grid voltage. The association among the DC link voltage V_{dc} and the line-to-line RMS grid voltage V_{LL,AC}, where m_a is the modulation index in the linear region, is specified in Eq. (29) [9].

$$V_{dc} \geq \frac{1.633}{m_a} V_{LL,AC} + \text{voltage drops} \quad (29)$$

The proposed control strategies are realized using MATLAB/SIMULINK environment by means of the parameters given in Table. 1 [5].

In order to show the response of the power control strategy during the unbalanced voltage condition, another simulation results have been extracted. In this case, The proposed control strategy has been inspected in case of unbalanced voltage conditions. An unbalanced voltage, resulting from unbalanced load, is applied at the grid side. The unbalanced voltage starts at 1.2 sec for duration of 2 sec. The grid voltage during unbalanced voltage has been shown in Fig.8.

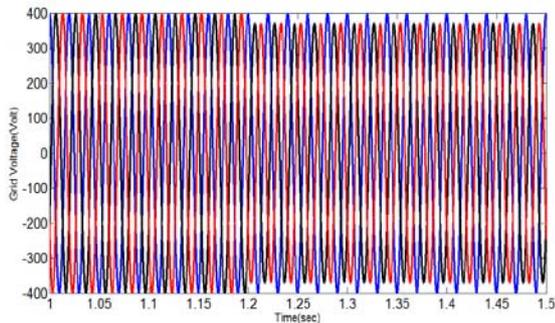


Fig.8 : The unbalanced grid voltages

Fig. 9 shows the 3-phase voltages; which are well regulated under the unbalanced disturbance.

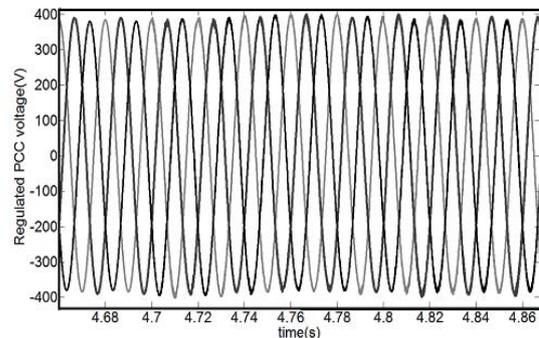


Fig.9 : Regulated grid voltage

From Fig.10 and Fig.11 the grid voltage and currents under the neuro-fuzzy controller have great improvement in case of Total harmonic distortion THD that was depicted in Fig.12.

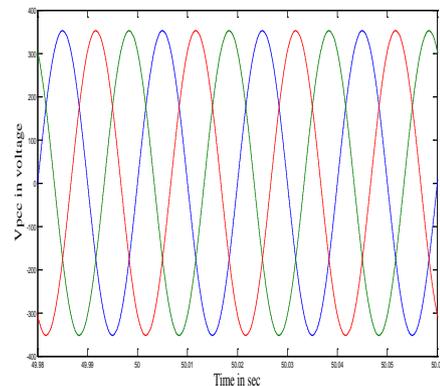


Fig. 10

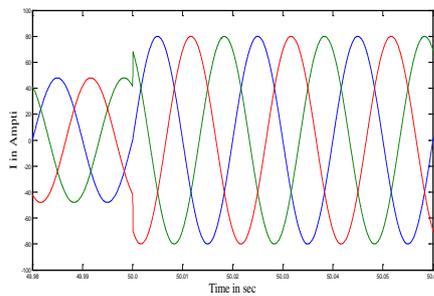


Fig. 11

From Fig.12 THD is only 3% in case of neuro-fuzzy controller and 15.27% in case of without neuro-fuzzy controller.

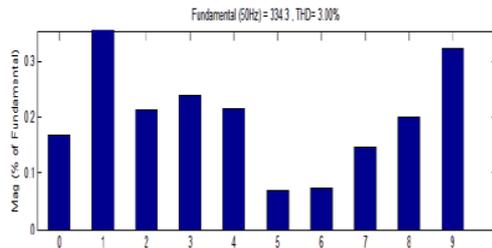


Fig. 12

The DC link voltage is shown in Figs.13. During the unbalanced voltage, there is an increase on DC link voltage but it is not much more than 10% of nominal value. In these conditions, to stabilize the dc-link power, the neuro-fuzzy controller manages the power flow between power sources.

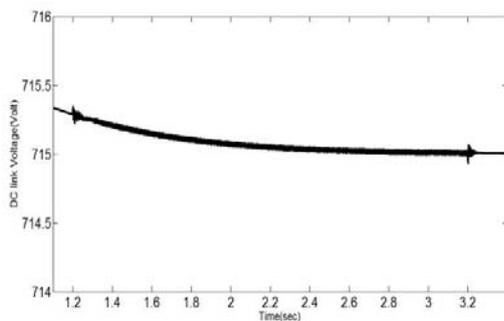


Fig.13: DC-link voltage

VI. CONCLUSION

This paper presents modeling, control and power control in a grid connected PV/Fuel Cell/Battery hybrid power generation system in a microgrid. Here SIMULINK/SIMPOWER was utilized to model the system and simulate a power flow control strategy. PV, fuel cell and battery subsystems with power electronic converters are modeled. In addition, to disseminate the power between power sources, the neuro-fuzzy power controller has been produced to settle the DC-link power. Our simulation results are shown to exhibit the viability and ability of proposed control strategy amid various operating conditions in utility grid.

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Development of Low Frequency Pulsed NQR/NMR Spectrometer

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Abstract- An FPGA based NQR spectrometer has been designed for detection of ^{14}N nuclei. The digital circuits required for NQR spectrometer i.e Pulse Programmer, DDS, digital receiver have been built inside FPGA. Combining FPGA chip with analog components, NQR spectrometer has been developed. ^{14}N from NaNO_2 is observed using same spectrometer. By adding a permanent magnet of uniform field NMR signal of proton as well as deuterium was also observed.

Keywords: *FPGA, NQR, NMR.*

GJRE-F Classification : *FOR Code: 290903p*



Strictly as per the compliance and regulations of :



Development of Low Frequency Pulsed NQR/NMR Spectrometer

Preeti Hemnani ^α, A. K.Rajarajan ^σ, Gopal Joshi, ^ρ & S. V. G Ravindranath ^ω

Abstract An FPGA based NQR spectrometer has been designed for detection of ¹⁴N nuclei. The digital circuits required for NQR spectrometer i.e Pulse Programmer, DDS, digital receiver have been built inside FPGA. Combining FPGA chip with analog components, NQR spectrometer has been developed. ¹⁴N from NaNO₂ is observed using same spectrometer. By adding a permanent magnet of uniform field NMR signal of proton as well as deuterium was also observed.

Keywords: FPGA, NQR, NMR.

I. INTRODUCTION

The nuclear magnetic resonance (NMR)[1] since its invention in the year 1946, has developed into a very useful and popular tool for material characterization and medical applications like magnetic resonance imaging(MRI). While the development of NMR as a technique itself is significant, the role of advancement in digital electronics in the instrumentation and techniques of NMR cannot be overstated. Since the invention of the original continuous wave NMR, digital signal processing (DSP) and advanced Fourier transform techniques have become integral part of modern day pulsed NMR technique. The specificity of NMR to the nucleus has made it more useful for purposes that are less popular than routine

characterization of biological molecules or MRI, where NMR of proton is mainly used. Nuclear Quadrupole Resonance (NQR) shares the same electronics and detection technique except for the presence of magnet. Observable in the non-cubic crystalline samples, NQR is not only nucleus specific but becomes compound specific making it a tool for detection, quantification and characterization of various chemicals for various purposes like remote detection of drugs, explosives or quantifying the chemicals in already packed medicines[1][2].

An NQR spectrometer for detection of nuclei ¹⁴N (frequency range up to 6 MHz) has been designed, constructed in Electronics Division, BARC is shown in Figure 1. The stable nitrogen ¹⁴N has natural abundance of 93.6% and nuclear spin I = 1 with its associated nuclear electrical quadruple moment. The ¹⁴N NQR transitions in various solids fall in the frequency range 0 to 6 MHz [3], hence the choice of the frequency band of our spectrometer. ¹⁴N NQR signal from sample of 20g of NaNO₂ was observed at 4.64MHz. Also by adding permanent magnet ¹H and ²H NMR signal from H₂O and D₂O was observed.

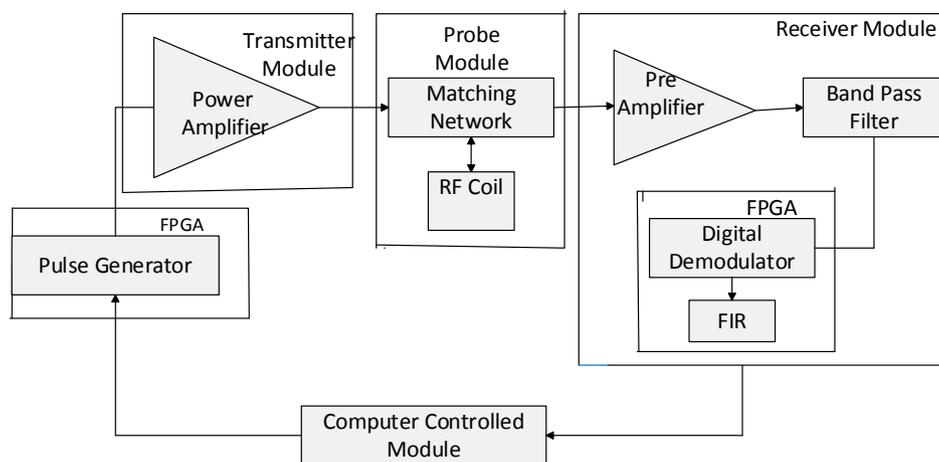


Figure 1 : Schematic diagram of FPGA based NQR spectrometer

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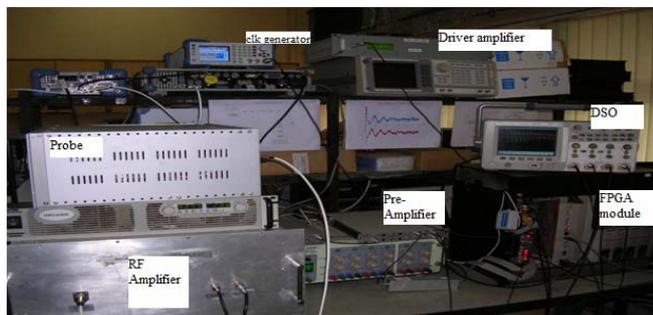


Figure 2 : NQR spectrometer developed in Electronics Division, BARC

II. INSTRUMENT DESCRIPTION

NQR instrument is designed and constructed using a digital technique which includes FPGA chip, ADCs and DACs. With the field programmability the digital part of NQR instrument could be constructed with FPGA resulting in compact and programmable NQR instrument with high sensitivity and suitable for applications such as detection of drugs, mines and plastic explosive in packages.

Specifications of the NQR instrument are 0-6MHz, pulse lengths 1-500 μ sec and radio frequency pulse power up to 200 watts, acquisition time 50 msec. The spectrometer consists of

- i) Transmitter which consists of RF power amplifier.
- ii) Probe which consists of coil which consists of RF tuning and matching circuit.
- iii) Receiver which consists of preamplifier, Band pass filter, ADC.
- iv) FPGA module which consists of pulse programmer, DDS, gate, quadrature demodulator, FIR low pass filter.
- v) Computer controlled module which interface for command/data transfer.

Block diagram of experimental setup is shown in Figure 1 and photograph is shown in Figure 2. In this experiment, a set of RF pulses is applied to pick up coil and the resulting magnetic moment is picked up by same coil. The radio frequency is generated by a direct digital synthesizer (DDS), and switched on and off by an RF switch controlled by pulse generator. These pulses are then amplified by a RF amplifier before going to the probe circuit. The probe circuit consists of pick up coil and pair of adjustable capacitors. The probe circuit is configured in such a way that with appropriate adjustment of capacitors, the impedance of circuit is 50.

By matching the impedance of the probe circuit to characteristic impedance of the coaxial cables carrying the signal and other components in the circuit (amplifiers etc), all of the power generated by the power amplifier is transferred to the probe circuit, and the signal generated by the probe circuit is efficiently transferred to the detection circuitry.

The precessing magnetic moment induced by applied pulses generated a voltage across the pickup coil, which is amplified by the low noise amplifier before being mixed with signal from DDS. This mixed down signal which is at frequency equal to difference between DDS frequency and frequency of the precessing spins is filtered.

a) Transmitter-RF Amplifier

A 500 W, 27 MHz Class AB RF power amplifier has been used for this NQR spectrometer. This has two stages and is housed in two different instrumentation bins. The total gain of the RF amplifier is 54 dB. Continuous or pulsed RF sinusoidal input to amplifier comes from FPGA (DDS and Pulse Programmer). In first stage 4 W RF power is generated and using 4:1 splitter 4 W RF power is split to get four 1W drive signals to four power stages. N channel enhancement type MOSFET has been used in power stages. Four 150 W power stages have been combined to get 500 W RF power is using 4:1 power combiner. The output power is available through a directional coupler on the front panel. The forward and reflected powers from the directional coupler are also routed to the front panel.

b) Probe

Probe circuit is a single coil pulsed resonance sample circuit which allows optimization in the transmitting and receiving end. In the transmitting mode the circuit is matched to transmitter output impedance 50 ohm and in receiving mode it is matched to optimum input impedance of pre-amplifier.

The probe circuit used here is parallel tuned LC circuit impedance matched to 50 ohms with a series capacitor (figure 3). The sample coil (L_{coil}) is made out of 17 AGW copper wire and has 32 turns of 20 mm diameter. The inductance of the coil is 6 μ H. The capacitors C_T and C_M are high voltage (5 kV) variable (5 pf – 125 pf) vacuum capacitors. In order to reduce the noise the probe circuit is shielded inside an aluminum box and is well grounded. The coils are made mechanically stable by potting them in resin based adhesive (Araldite®).

The capacitors are varied in order to tune the circuit to the resonance frequency and match the circuit to 50 ohms for maximum power transfer from the transmitter. The approximate values of C_T and C_M can be calculated by following Equations [4].

$$\omega^2 LC_T = 1 \quad (1)$$

$$\frac{Q \omega L C_M^2}{C_T + C_M} = 50 \quad (2)$$

$$C_T = \frac{1 - \sqrt{R/50}}{\omega^2 L} \quad (3)$$

$$C_M = \frac{\sqrt{R/50}}{\omega^2 L} \quad (4)$$

The tuning and matching are achieved by maximizing the forward power and minimizing the reflected power. The forward and reflected power is

monitored using the directional coupler built in the transmitter.

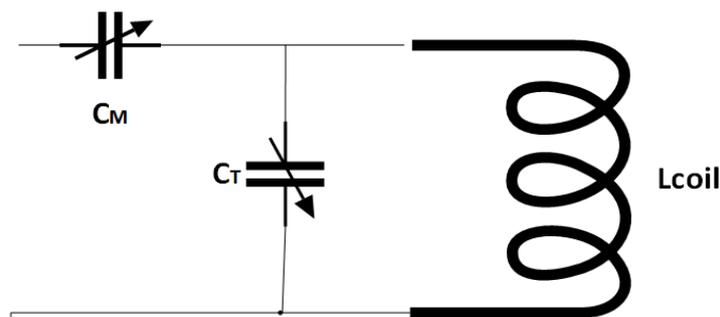


Figure 3 : Probe

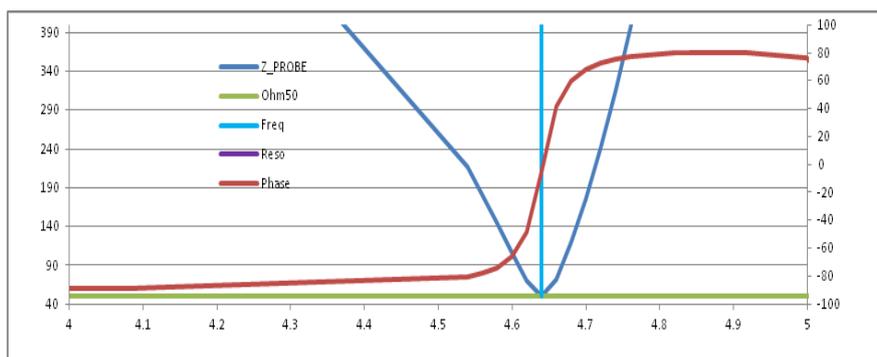


Figure 4 : Impedance of Probe vs Frequency. Horizontal axis is Frequency in MHz, Vertical axis in left is Z_{Probe} in Ohms, Vertical axis in right is phase in degrees

Powder sample ($NaNO_2$) is packed in test tube of 18 mm diameter and 46 mm length. The size of the coil and the test tubes are chosen in order to maximize the filling factor.

okup table), and a DAC. It has ability to produce two independent outputs 90° out of phase, which are mandatory for quadrature detection. Output frequency of DDS is given by equation no. 5.

c) Direct Digital Synthesis

Direct Digital Synthesis (DDS)[5] is a method of producing an analog waveform by generating the sinusoidal signal in digital form and then performing a digital to analog conversion. The operations within a DDS device are primarily digital therefore, it offers fast switching between output frequencies, fine frequency resolution, and operation over a broad spectrum of frequencies.

$$F_{out} = \frac{M \times F_c}{2^n} \tag{5}$$

- where M is Phase tuning word (PTW)
- F_{out} is Output frequency of DDS
- F_c is Internal reference clock frequency (CLK)
- n is Length of phase accumulator

The digital part of the phase tunable and frequency fixed DDS, denoted here as DDS, is built inside FPGA as a core module, while the non-digital parts, i.e., digital to analog converter (DAC) and filter, are outside the FPGA as shown in Figure 5. The output level of a DAC is updated in synchronous with a master clock. As a consequence of discrete change in the output voltage at clock rising edges, the output of a DDS circuitry contains signal components with the image frequencies in addition to the fundamental one. The output signal is passed through a filter to select fundamental frequency.

The resolution of DDS in spectrometer designed is $F_c/2^{22} = 10.96$ Hz.

Changes in the value of M results in immediate and continuous phase changes in output frequency. As the output frequency is increased the number of samples per cycle decreases, since sampling theory states that at least two samples per cycle are required to construct the output, the maximum fundamental output frequency of DDS is $F_c/2$. However for practical applications the output frequency is limited to somewhat less than that the maximum, improving the quality of reconstructed waveform and permitting the filtering of output.

The main components of a DDS circuitry are a phase accumulator, phase to amplitude converter (sine lo

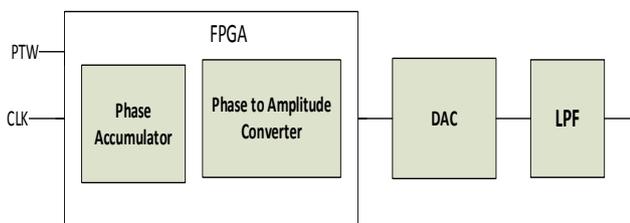


Figure 5 : Direct Digital Synthesizer

d) Programmable Pulse Generator

Finite state machine (FSM) was written for programmable pulse generator using state diagram editor of active HDL software. FSM was then converted to VHDL code reproduces the pulse programmer inside the FPGA. The function of pulse programmer is to generate timing sequences for enabling transmitter, receiver, acquisition, RF modulating pulse. In addition pulse programmer also controls the phase of RF pulses as per the requirement for the observation of free

induction decay (FID) and spin echo by triggering the DDS at appropriate phase points.

Following are pulses that are generated by pulse generator. They control various parts of the spectrometer.

1. Transmitter Enable.(1-200 μ sec)
2. Receiver enable.(1 – 11 sec)
3. RF modulating Pulse.(1-100 μ sec)
4. Acquisition Trigger (1 -10 sec)
5. RF Phase Control (0° , 90° , 180° , 270°)

Transmitter enable pulse is to enable the RF power amplifier in between which RF pulses are send to the probe. RF modulating pulse at resonance frequency is send to the probe for the exciting nuclei sitting in a probe. After the RF pulses the pulse programmer disables the transmitter and enables the receiver by receiver enable pulse. Now the receiver is ready to receive the signal and send to digital quadrature detector. The pulses are shown in Figure 6.

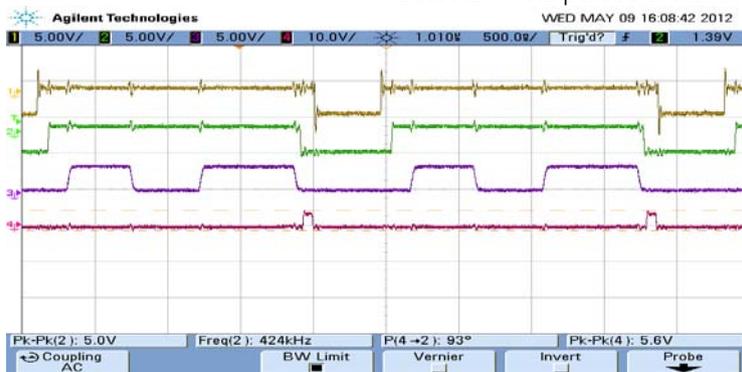


Figure 6 : Start,TxEn,RF_pulse,RxEn

The DDS is programmed to generate an RF frequency (reference frequency). This signal is routed through the phase shifter which is controlled by the pulse programmer. The phase shift is to provide pulses along the different axes in the vector model. By convention,

- phase shift of 0° is an x-phase pulse,
- phase shift of 90° is an y-phase pulse
- phase shift of 180° is an -x-phase pulse

phase shift of 270° is an -y-phase pulse

e) RF Modulating pulse

RF modulating pulse can be one pulse sequence for observation of FID or a two pulse sequence for observation of spin Echo.

VHDL code has been written for the pulses to be 90° at x and 180° at y. The two pulse sequence is shown in Figure 7.

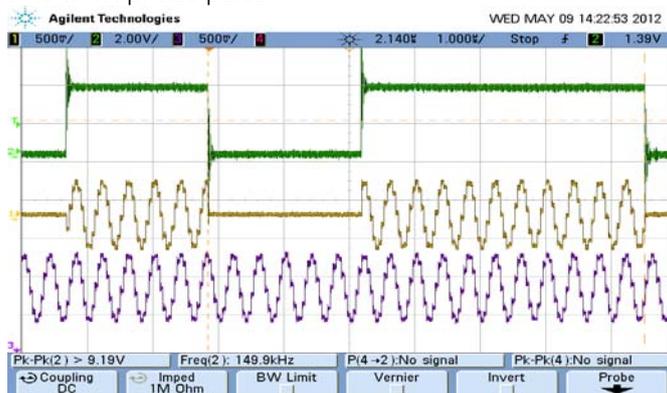


Figure 7 : Two Pulse (90° at x and 180° at y) on Scope

f) *Crossed Diodes and Quarter Wave Impedance Transformer*

The high power output of transmitter to the probe needs to be isolated from the sensitive receiver amplifier. This is achieved using crossed diodes and quarter wave lines [6]. Between the RF power amplifier and the probe there is a pair of cross diodes which show a high series impedance when the transmitter is off and a low impedance during the pulses. Thus between the pulses, the power amplifier and its associated noise is isolated from the probe circuit. The signal from the probe circuit passes through a quarter wave line to reach another pair of cross diodes which are shunted to ground at the input of pre-amplifier. The diode shorts the preamp end of the cable when transmitter is on, thus protecting the sensitive pre-amplifier from high RF power out from the power amplifier. Between pulses, the voltage across the diodes is too small to turn them on, and they act like an open circuit, letting the NQR signal pass to the preamplifier.

Though at high frequencies a suitable length of a co-axial cable like RG-58 itself can serve the purpose of a quarter wave line, at the frequencies of our interest (viz. < 6 MHz), co-axial cables are inconvenient because of the long lengths. So we have used 50 Ohm compatible quarter wave sections following the method given by Fukushima et al [7].

A quarter wave transmission line acts a transformer which transforms its output impedance according to the equation,

$$Z_{output} = \frac{Z_0^2}{z_{input}} \tag{6}$$

where $Z_0 = 50$ is the characteristic impedance of the transmission line. Thus, during the pulses, when the shunt diodes are acting as short, the input impedance of the transmission line is infinite acting as if the receiving circuit were completely disconnected from the probe.

The equivalent of $(\lambda/4)$ cable for operating frequency as 4.64 MHz for NaNO_2 is a π network shown in figure 8 a.

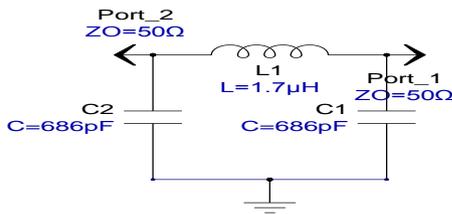


Figure 8 a) : Equivalent of $(\lambda/4)$ cable

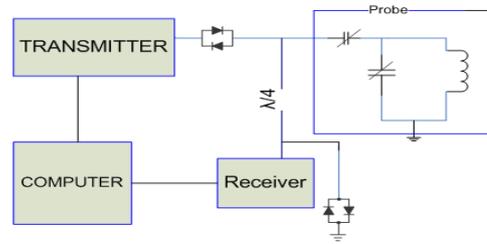


Figure 8b) : Block Diagram of Spectrometer showing cross diodes

g) *Pre-Amplifier*

NQR signal is expected to be of order of -100 dBm [8] so it needs to be amplified considerably before it can be observed on an oscilloscope. Three stages, each of which contains two amplifiers (BMC 1124, broadband RF amplifier, gain 14 dB) are connected in series as preamplifier with a gain of 84 dB and noise figure of 6.74 dB to achieve necessary level of amplification of NQR signal. Low pass filters (5 MHz) are connected after every stage to reduce Noise.

At the end of preamplifier band pass filter of bandwidth 500 KHz center frequency 4.64 MHz is cascaded to further reduce noise thus improving the signal to noise ratio.

h) *Digital Quadrature Detection*

The NMR receiver design is extremely important since it directly determines the final spectrum quality. The NMR signal is first amplified to a level of perhaps several hundreds of millivolts. The signal is then passed to ADC. The ADC converts the signal from voltage to data points. This signal is then demodulated in FPGA using mixer with I and Q components of reference signal which comes as DDS output.

Principle

DQD technique[9],[10] works on lock in amplification technique where signal is multiplied to I and Q components of reference signal (figure 9). If signal is $S(n)$ then

$$S_I(n) = S(n) * \text{Cos}(\omega_0 n)$$

$$S_O(n) = S(n) * \text{Sin}(\omega_0 n)$$

If $S(n) = \text{Sin}(\omega n)$

Then

$$S_I(n) = \text{Sin}(\omega - \omega_0)n + \text{Sin}(\omega + \omega_0)n$$

$$S_O(n) = \text{Cos}(\omega - \omega_0)n - \text{Cos}(\omega + \omega_0)n$$

The lower frequency component is the desired signal. In the demodulation process the signal oscillating at frequency $(\omega - \omega_0)$ is of interest and component at $(\omega + \omega_0)$ are dropped off with lowpass FIR filter.

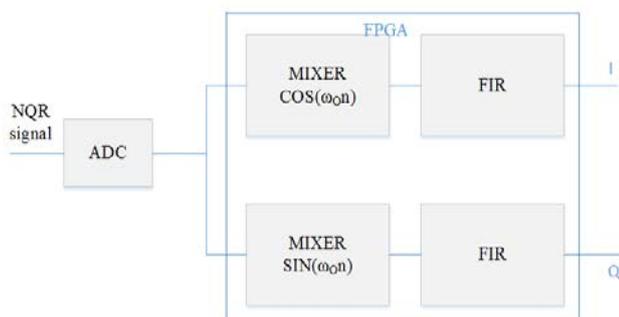


Figure 9 : Digital Quadrature Detection

i) FIR filter

Inside the FPGA, each of the demodulated I and Q components of the signal is made to pass through a finite impulse response FIR low pass filter, generated using fdatool of MATLAB. The FIR filter used is 31-stage, Hamming-window filter with a cut-off frequency of 30 kHz and sampling frequency 2.875 MHz.

The FIR digital filters with various cutoff frequencies can be incorporated, out of which users can select the appropriate one according to the sampling interval, or spectral width, of an individual NMR experiment.

j) Signal accumulator

The signal intensity of ^{14}N NQR seldom exceeds the thermal noise signal therefore it can be detected with high degree of reliability after multiple acquisitions. A memory module for storing the NQR signal is also prepared inside the FPGA using dual port RAM module. In the current NQR spectrometer, up to 16384 data points can be stored for each of the in-phase and quadrature signals. The stored data can be transferred to PC every scan or can be averaged n times ($n \leq 4096$) before data transfer.

III. EXPERIMENTAL RESULTS

a) NQR/NMR signal Detection

Two popular methods of observing NQR/NMR signals are: i) observe FID using a single pulse excitation. ii) Observe spin echo using a double pulse sequence. The choice of the sequence depends mainly on the relaxation time (T_2^*) of the sample. For a long relaxation time of milliseconds as in the case for ^{14}N signal from NaNO_2 , a single pulse sequence is appropriate and for a short relaxation time as in the case of ^1H and ^2H double pulse sequence is used to observe a spin echo.

The main challenge for NQR techniques is the extremely poor signal to noise ratio (SNR). To improve SNR, many repetitions of the experiment are necessary. The most commonly method is to use repeated single RF pulse and acquire NQR signal after each pulse. The

rate at which RF pulse has to be repeated depends on physical parameters of nuclear relaxation which are spin-spin relaxation and spin lattice relaxation. Spin lattice relaxation time is denoted by T_1 determines the time necessary to regain its original thermal equilibrium state and gives bound to how quickly a pulse sequence can be repeated. The spin-spin relaxation time denoted by T_2 indicates decoherence and thus determines the RF pulse length. In practice we can apply a pulse sequence of length T_2 and repeat the pulse sequence every T_1 . For most of explosives the relaxation times are very long which lead to long detection times [11].

The NQR Spectrometer (Fig 1) designed has been used to observe an NQR signal from Sodium Nitrite sample.

Fig 10 shows the ^{14}N NQR signal in 20g of Sodium Nitrite. The observation frequency is 4.642 MHz where as the signal is off resonant by about 2500 Hz resulting in oscillatory FID. RF excitation pulse length of 20 μsec and power of 120 W was used for excitation. The entire cycle is repeated after every 0.5 s (large compared to the spin lattice relaxation time of 0.7 ms). The signal strength is at the expected level of 6 μvolts . The NQR signal shown in Figure 10 is averaged for 1024 times.

The NQR spectrometer was modified to NMR spectrometer by placing the coil in a permanent magnet. Here sample in a coil is placed between poles of a horse shoe magnet of magnetic field 1.35 K Gauss and spin echo experiment was carried out. A small quantity of ferric nitrate is added in order to reduce the T_1 of pure water and the proton signal from water is observed.

Fig 11 shows the spin echo (^1H from $\text{H}_2\text{O}:\text{FeNO}_3$). The observation frequency is 5.765 MHz We used $t_1 = 5 \mu\text{sec}$, $t_2 = 10 \mu\text{sec}$, $\tau = 200 \mu\text{sec}$, RF excitation power was about 70 W. The entire cycle was repeated after every 0.5s. The signal strength without averaging is 50 μvolts . The signal shown in figure 11 was averaged for 256 times.

Also Deuterium NMR was observed using a magnet of magnetic field of 3.85 K Gauss. The deuterium signal is shown in Figure.12. The observation frequency is 3.855 MHz. $t_1 = 5 \mu\text{sec}$, $t_2 = 10 \mu\text{sec}$, $\tau = 2.5 \text{ msec}$. The signal strength without averaging is 8 μvolts .

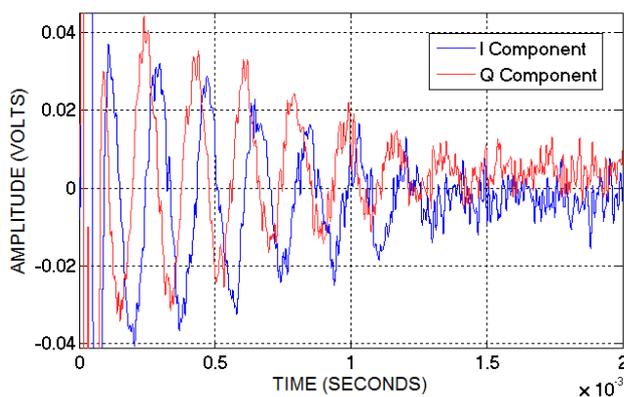


Fig. 10 : ^{14}N NQR signal from NaNO_2

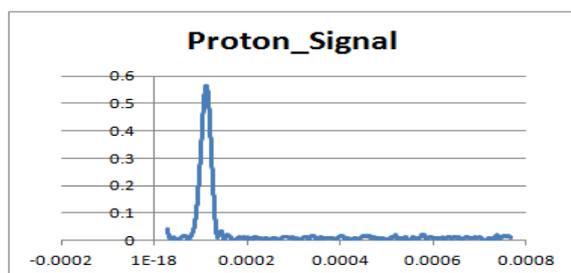


Fig. 11 : ^1H NMR signal from H_2O . The horizontal axis is time in seconds and vertical axis shows signal strength in volts

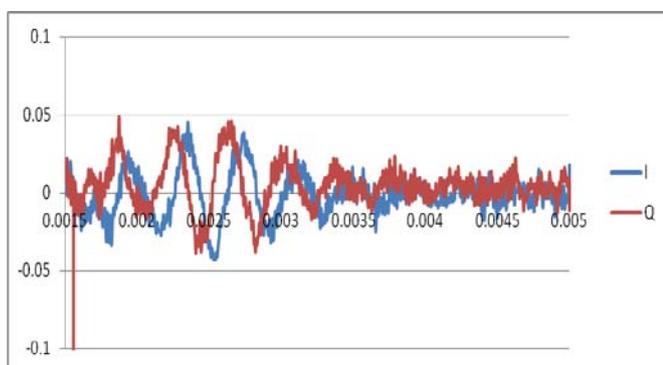


Fig. 12 : ^2H NMR signal from D_2O . The horizontal axis is time in seconds and vertical axis shows signal strength in volts

IV. CONCLUSION

This spectrometer can further be developed into a miniature spectrometer by combination of RF amplifier, receiver module and FPGA module on one board and thus enhances opportunities for novel and exciting NQR/NMR experiments like explosive detection, mine detection etc.

V. ACKNOWLEDGMENT

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A Planar CPW Antenna Loaded with Rectangular Slot for Triple Bands Operation

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Abstract- In this paper a planar CPW antenna loaded with rectangular slot is presented. The proposed antenna offers three frequency bands and hence suitable for triple bands wireless applications. The proposed geometry has hexagonal shaped radiator loaded with a rectangular slot to excite three resonant frequencies in the UWB frequency range. The three resonances of triple bands obtained are at 5.9GHz, 9.9GHz, and 14.4GHz. The antenna was designed and developed on easily available low cost FR-4 glass epoxy substrate. The proposed antenna's prototype was developed for its validation and found reasonable agreement between the simulated and measured results.

Keywords: *CPW fed antenna, planar antenna, triple bands antenna.*

GJRE-F Classification : *FOR Code: 291701*



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I. INTRODUCTION

The Federal Communication Commission (FCC) allocated the frequency band spectrum from 3.1 to 10.6 GHz for monetary communication applications in year 2002 [1]. This resulted in the development of several antennas which operate in the ultra wideband (UWB) range. It is also expected that in this range frequency satisfactory radiation properties are required. An UWB antenna which satisfies the more requirements like a small size, consistent group delay, omnidirectional radiation patterns, and gain beyond whole band [2, 3]. There are several works reported in literature on these kinds of antennas [3-15]. By adding half wavelength V-shaped slot on radiating patch, UWB antenna achieves sharp band notched characteristics [3]. A lower pass band, 2.4 GHz Bluetooth band (2.4 – 2.484 GHz), can be realized by adding a pair of U-

shaped parasitic strips bilaterally beside the feed line which covers whole UWB band [4].

In [7], by inserting an U shaped slot on radiating patch which produces band notch characteristics. The main goal in UWB antenna design is achieving the wide impedance bandwidth with high radiation efficiency. Section 2 describes the basic geometry and its operation. Geometry optimization procedure is covered in Section 3. Experimental validation of the proposed antenna is presented in Section 4. Finally, Section 5 concludes the work carried out and guidelines the future scope.

II. ANTENNA GEOMETRY

Figure 1 shows basic geometry of the proposed antenna. The proposed antenna is having a low profile geometry with overall dimensions of 24 x 25mm x 1.6mm ($L \times W \times h$). The substrate used for design and fabrication is FR4 glass epoxy substrate with relative permittivity of 4.4, thickness of 1.6mm, and loss tangent equal to 0.02. The geometry is basically a CPW fed monopole antenna. An elliptical slot is etched in the ground with major axis radius of 11.55 mm and minor axis radius of 10 mm. Hexagonal stub is attached to the signal conductor of the CPW line to ensure the impedance matching. Also, a rectangular slot is made on the hexagonal stub to excite multiple bands and to enhance their bandwidths. The other dimensions are mentioned in Table 1 based on the optimization procedure discussed in Section 3.

Table 1 : Dimensions of the optimized geometry

Parameter	L_1	W_1	L_2	L_3	L_s	W_s	W_2	W_3	g_1	g_2	a	b	c
Values (mm)	24	25	2.59	3.6	7.2	7.1	5.29	2.2	0.1	1	10	11.55	5.66

III. GEOMETRY OPTIMIZATION AND DISCUSSIONS

This section covers the geometry optimization by varying some parameters of the antenna geometry. The parameters utilized for optimization are gap g_1 ,

width of signal conductor (W_3) of CPW feed, length of rectangular slot (L_s), and the width of rectangular slot (W_s). High frequency structure simulator (HFSS-v.13) [16] was used to carry out the parametric optimization.

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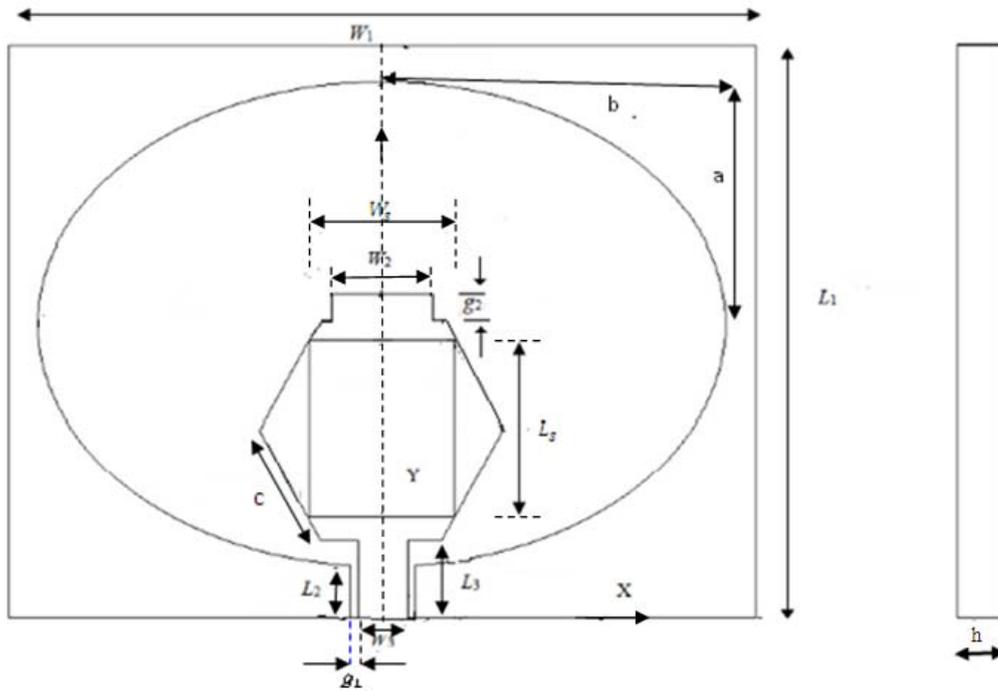


Figure 1 : Basic geometry of the proposed antenna (left: top view; right: cross sectional view).

a) Variation of Gap (g_1)

The gap between signal conductor and ground (g_1) was varied from 0.1 to 0.2 in steps of 0.05 mm by keeping all other parameters constant. Effect of g_1 on

S_{11} characteristics is presented in Figure 2. From Figure 2 it may be noted that impedance matching may be fine tuned with this parameter. From this study the gap value of $g_1 = 0.1\text{mm}$ was noted as an optimum.

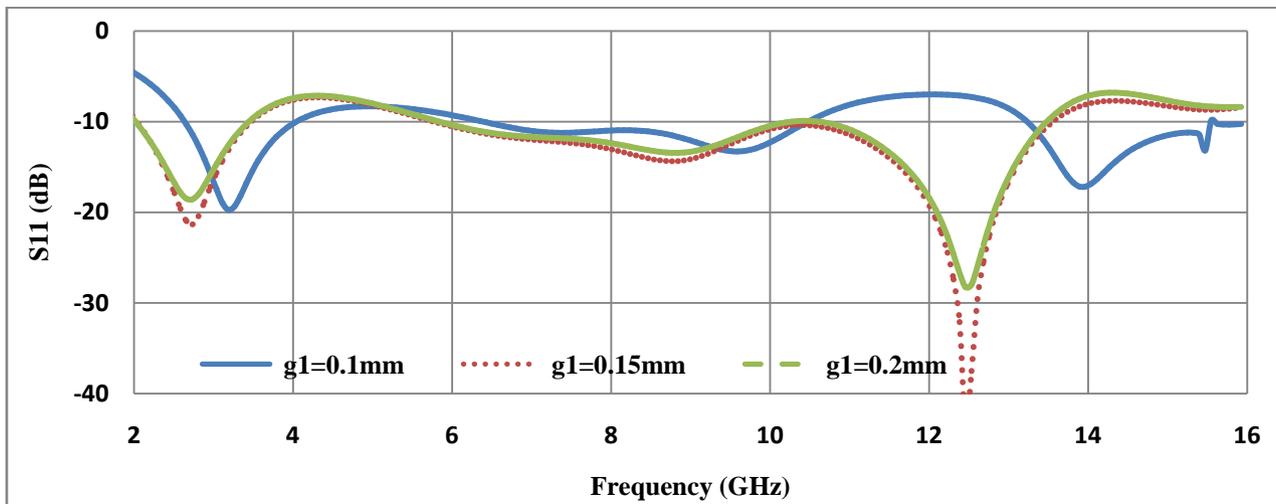


Figure 2 : The effect of the length g_1 on reflection coefficient characteristics.



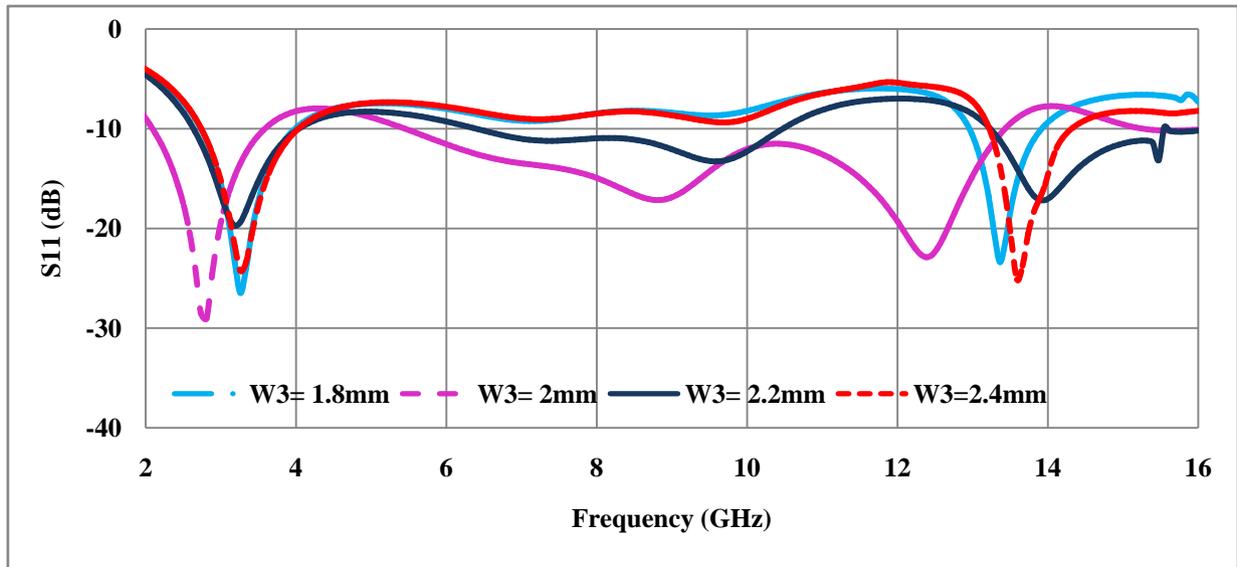


Figure 3 : The effect of the signal conductor width W_3 on reflection coefficient characteristics.

b) Effect of Length of Rectangular Slot (L_s)

In another effort, rectangular slot length (L_s) was varied from 5.7 mm to 7.2 mm in steps of 0.5mm with all other parameters kept constant. Effect of variation of rectangular slot's length on reflection coefficient

characteristics are presented in Figure 4. In this observation, a slot value of $L_s = 7.2$ mm offered the optimum impedance bandwidth. It may be noted that slot length beyond 7.2mm cuts the edges of the hexagonal signal conductor stub.

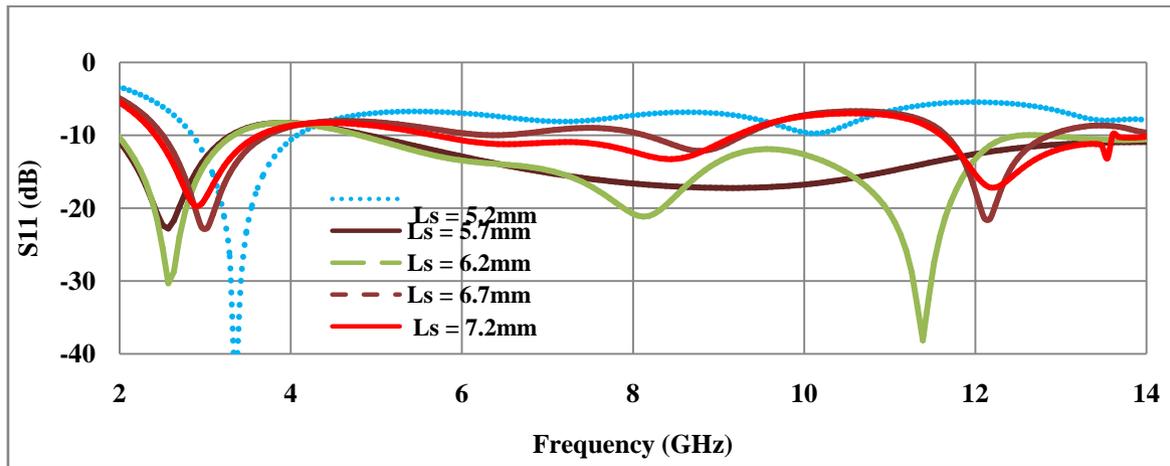


Figure 4 : The effect of the length of rectangular slot L_s on reflection coefficient characteristics.

c) Effect of Width of Rectangular Slot (W_s)

Finally, the width of rectangular slot was varied from 5.1 mm to 7.1 mm in steps of 0.5 mm by keeping all other parameters constant. The effect of variation of W_s on the antenna's input characteristics are presented in Figure 5. These characteristics indicate that a rectangular slot width of $W_s = 7.1$ mm offers the optimum performance.

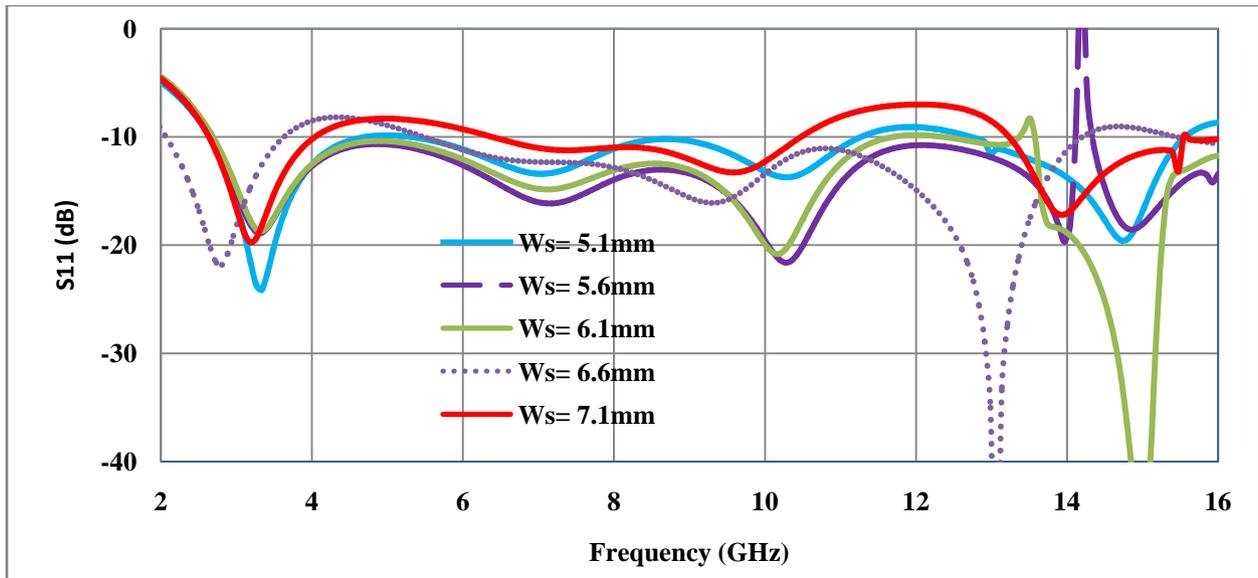


Figure 5 : The effect of the Width of rectangular slot W_s on reflection coefficient characteristics.

IV. EXPERIMENTAL VALIDATION OF THE GEOMETRY AND DISCUSSIONS

The prototype of antenna geometry shown in Figure 1 was fabricated and tested experimentally for its validation. The dimensions used for prototype development are as listed in Table 1. Substrate used for development is an FR4 glass epoxy material whose height is 1.6mm and having a relative permittivity of 4.4 with dielectric loss tangent of 0.02. The photograph of

the fabricated design is as shown in Figure 6. Antenna's reflection coefficient parameters were measured using Agilent's network analyzer. Measured characteristics are compared with simulated values and presented in Figure 7. Although, a mismatch was observed due to fabrication inaccuracies, tri band operation was observed. Three resonances are obtained at 5.9GHz, 9.9GHz, and at 14.4GHz.

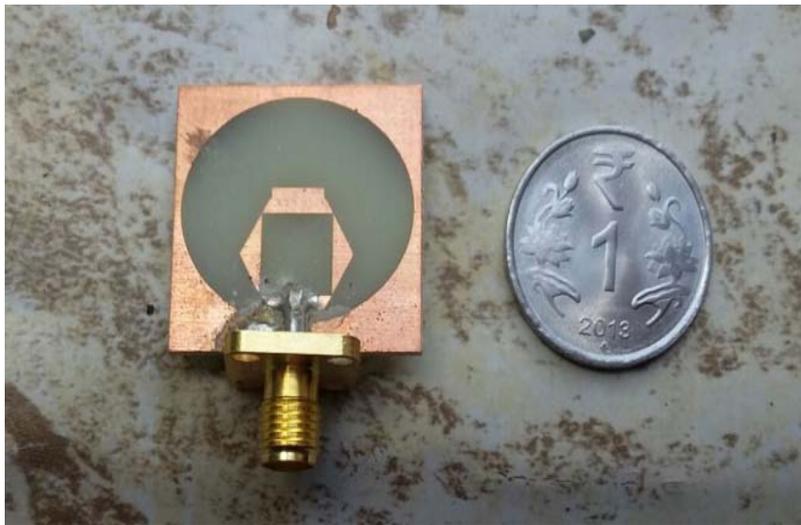


Figure 6 : Photograph of the fabricated prototype.

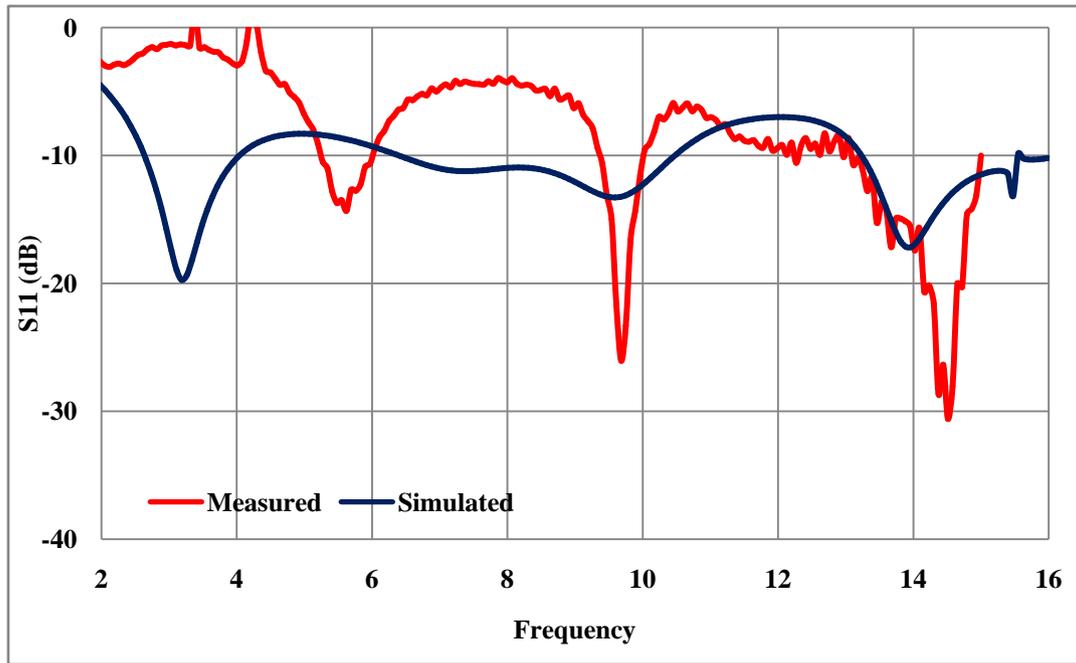
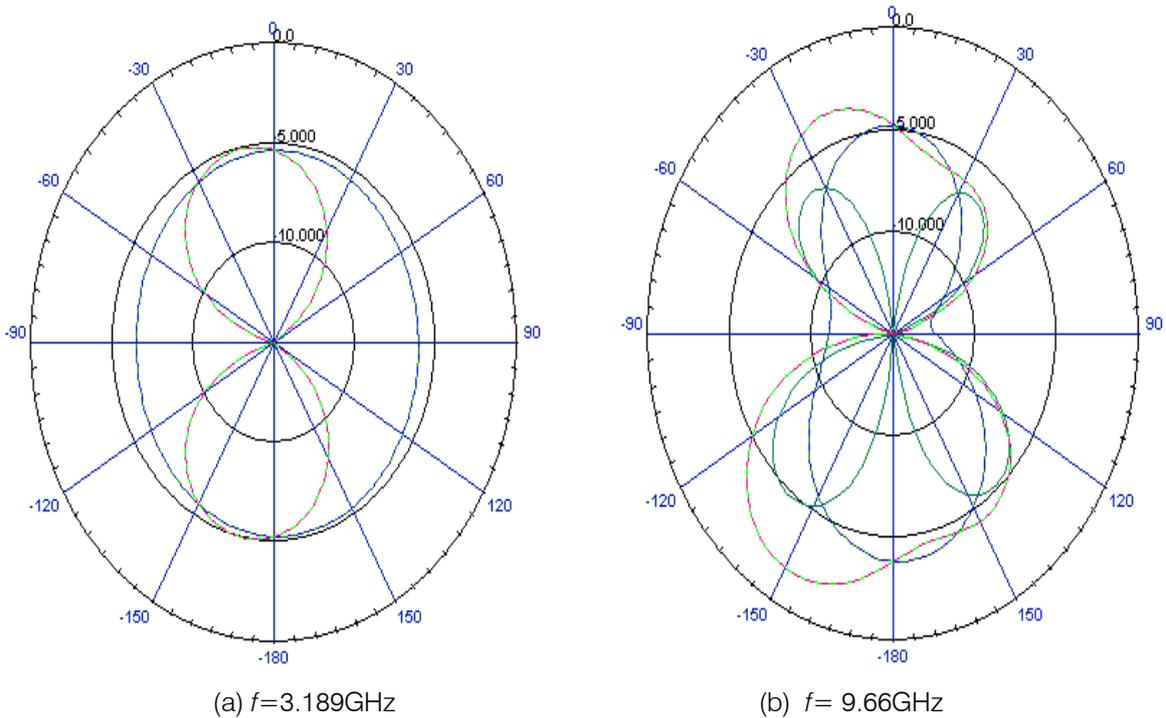


Figure 7 : Comparison of measured and simulated reflection coefficients.

Radiation patterns are plotted at three different frequencies are depicted (Figure 8) to demonstrate the proper working of antenna.



(a) $f=3.189\text{GHz}$

(b) $f= 9.66\text{GHz}$

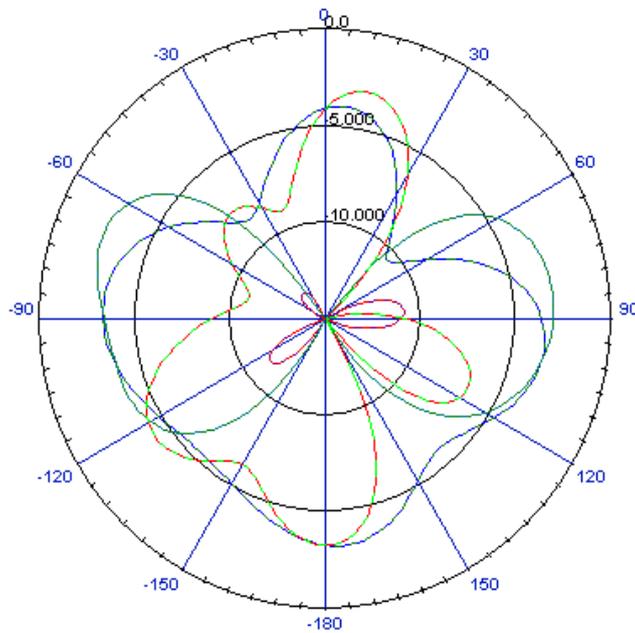
(c) $f = 13.96$ GHz

Figure 8 : Radiation patterns at three resonances of the antenna.

V. CONCLUSIONS

A planar patch antenna fed with CPW feed has been presented for tribands operation. Proposed antenna is basically a monopole antenna. A rectangular slot was loaded to excite three resonance bands. Slot and hexagonal dimensions are tuned for impedance matching of antenna. Three resonances obtained are at 5.9GHz, 9.9GHz, and at 14.4GHz. Stable radiation patterns have been obtained across the bands of operation. The proposed antenna is suitable for tri-bands applications. The future work includes the bandwidth optimization of the three frequency bands.

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From Hertz-Heaviside Electrodynamics to the Trans-Coordinate Electrodynamics

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Abstract- The conclusion about the absence in them of the mathematical means of the adequate description of passage from one inertial reference system to another because of the use by them of particular derived field functions on the time, which completely tie electrodynamic process to one concrete frame of reference, is made on the basis of the critical analysis of extraction from the equations of the electrodynamics of ideas about the space and period. Is proposed new approach to the development of the mathematical apparatus for electrodynamics in the direction of the more adequate description of passage from one inertial reference system to another due to the introduction into the examination of the trans-coordinate equations, which use new Galilean and trans-coordinate derivatives of field functions. This generalization of electrodynamics assumes the dependence of electromagnetic field and electric charge on the speed of the motion of observer, caused not by the geometry of space-time, but by physical nature of the very field within the framework of gipercontinual ideas about the space and the time. Is obtained the new trans-coordinate formulation of Maxwell equations for the case of isotropic homogeneous medium without the dispersion, which generalizes the traditional formulation of Hertz-Heaviside for the same case. Are given Maxwell equations in the integral and differential forms in the idea of Hertz-Heaviside and in the transcoordinate idea.

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From Hertz-Heaviside Electrodynamics to the Trans-Coordinate Electrodynamics

A. S. Dubrovin ^α & F. F. Mende ^σ

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I. INTRODUCTION

In the initial form the system of equations of classical electrodynamics was recorded by Maxwell in his famous treatise [1] with the use of quaternion calculation within the framework of classical ideas about the space and time, that allow the Galileo conversions upon transfer from the examination of electromagnetic field in one inertial reference system to the examination of the same field in another inertial reference system. However, it was immediately explained that the apparatus for quaternion calculation in mathematics was developed not so well so that physics they could it successfully apply to the wide circle of the tasks of electrodynamics. In order to draw into the electrodynamics the simpler and more effective means of mathematical physicists, Hertz and Heaviside reformulated Maxwell equations from the language of quaternion calculation to the language of vector analysis.

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At that time it seemed that the formulation of Hertz-Heaviside is equivalent to the initial formulation of Maxwell, but now already it is possible to establish that the equations, obtained by Hertz and Heaviside, are essential simplification in Maxwell equations in the quaternions, moreover this simplification relates not only to their mathematical form, but also (that most important!) to their physical content, since in this case equations were deprived naturally Galileo- invariance of inherent in them. Nevertheless for the concretely undertaken inertial reference system (but not their totality) the equivalence of formulations occurred, by virtue of which the formulation of Hertz-Heaviside it obtained the deserved acknowledgement of scientific association it extruded in the theoretical and applied research the formulation of Maxwell himself.

Despite the fact that Maxwell equations both in the formulation of Maxwell himself and in the formulation of Hertz- Heaviside, are obtained within the framework classical ideas about the space and of time, who use Galileo conversions, subsequently precisely of Maxwell equation they became the theoretical prerequisite of the creation of the special theory of relativity (SR). As convincingly shown, for example, in [2], be SR it consists of the identification of the natural geometry of the electromagnetic field, described by Maxwell equations, with the geometry of world physical space-time. And now already in the contemporary works on the electrodynamics (typical example – the work [3]) of Maxwell equation they are examined in the four-dimensional pseudo-Riemann space-time).

Is it possible to return to Maxwell equations the original Galileo- invariance within the framework of certain new, its kind of neoclassical ideas about the space and the time, without rejecting the use of an apparatus of vector analysis during writing of equations? In this work we will show that the answer to this question is affirmative.

II. CONCEPTUAL APPROACH

In the classical mechanics particle dynamics is described by the differential equations for its radius-vector, which use usual derivative of the second order on the time. Specifically, its use ensures the Galileo-invariance of equations. If we connect the set of massive material points by weightless elastic threads into the united string, i.e. fluctuation will be described by the Galileo- invariant system of differential equations. But if

we complete passage to the limit, after fixing the number of material points to infinity, and their mass and the length of separate threads – to zero, then we will obtain the one-dimensional wave equation (equation of vibrations of string), not invariant relative to the Galileo conversions, but invariant relative to the group of pseudo-orthogonal conversions (hyperbolic turnings, which preserve pseudo-Euclidean certificate). The culprit of this strange and unexpected metamorphosis upon transfer from “material- point mechanics to continuous medium – this passage to the limit with the substitution by usual derivative to the quotient, which, generally speaking, is analytically legal 4], but it narrows the region of the physical applicability of equation. The real wave process of mechanical vibrations of string remains Galileo- invariant, but its equation is already deprived of the mathematical means of the description of passage from one inertial reference system to another, and completely ties process to one concrete frame of reference, attaching in it the ends of the string. So classics- field natural-science paradigm revealed fundamental contradiction between the continuity and the discretion [5-6], not overcome, until now, but led to the celebration in theoretical physics of the doubtful principle of the geometrization [7].

The discovery wave equation in the mechanics did not lead to the revision of ideas about the space and the time, but to this led the discovery the same equation in the electrodynamics. In the theory of relativity the corresponding group of pseudo-orthogonal conversions for the electromagnetic waves in the vacuum (Lorenz conversion) obtained status of the subgroup of the motion of the certificate of united world physical space-time. But appears doubt about the justification of the use of traditional equations of electrodynamics, in particular, wave equation, for the adequate extraction of them of ideas about the space and the time. Easily to assume that these equations, using partial derivatives of field functions on the time, similar to the equation of mechanical fluctuations, are simply deprived of the mathematical means of the adequate description of passage from one inertial reference system to another and so completely they tie process to one concrete frame of reference. The question of the possibility of the suitable refinement or generalizing the equations of electrodynamics so arises, beginning from the equations of the induction of electric field by magnetic and magnetic – electrical. The thorough study of this problem in [8] led to the appearance of an idea about the fact that this improvement of electrodynamics must assume existence of the dependence of electromagnetic field on the speed of the motion of observer, caused not by the geometry of space-time, but by physical nature of field.

In the theory of relativity the electromagnetic field also depends on the speed of the motion of observer, but it is only defined by example through the

dependence on it of the intervals of time and spatial distance (Lorenz conversion), the relativistic invariance of electric charge occurs result of which. However, the more fundamental (direct) dependence of field on the speed is combined with the dependence even absolute value of electric charge. Until recently this not invariance of charge was confirmed only by indirect empirical data, which were being consisted in the appearance of an electric potential on the superconductive windings and the tori during the introduction in them of direct current, or in the observation of the electric pulse of nuclear explosions [9].

In particular, 9 July 1962 with the explosion in space above Pacific Ocean of H-bomb with the TNT equivalent 1,4 Mt. according to the program of the USA «*Starfish* » the tension of electrical pour on she exceeded those forecast by Nobel laureate Bethe in 1000 once. with the explosion of nuclear charge according to the program “*Program K*”, which was realized into the USSR, the radio communication and the radar installations were also blocked at a distance to 1000 km. It was discovered, that the registration of the consequences of space nuclear explosion was possible at the large (to 10 thousand kilometers) distances from the point of impact. The electric fields of pulse led to the large focusings to the power cable in the lead shell, buried at the depth about 1 m, which connects power station in Akmola with Alma-Ata. Focusings were so great that the automation opened cable from the power station.

However, 2015 was marked by the already direct experimental confirmation of this phenomenon as a result of detection and study of the pulse of the electric field, which appears with the warming-up of the plasma as a result of the discharge through the dischargers of the capacitors of great capacity [9]. It turned out that in the process of the warming-up of plasma with an equal quantity in it of electrons and positive ions in it the unitary negative charge of free electrons, not compensated by slower positive ions, is formed.

This fact contradicts not only the classical, but also relativistic conversions of electromagnetic field upon transfer from one inertial reference system to another, testifying about the imperfection not only of classical, but also relativistic ideas about the space and the time. Idea about the fact that the promising electrodynamics must assume existence of the dependence of electromagnetic field on the speed of the motion of observer, caused not by the geometry of space-time, and by physical nature of field, which does not assume the invariance of electric charge, was developed in a number of the work of F. F. Mende, beginning [8]. In these works, in particular, in [8, 9] is given the substantiation of introduction into the electrodynamics instead of the classical and relativistic

new conversions of electromagnetic field, which was called the Mende conversions.

However, the sequential development of this radical idea, as not the invariance of charge, requires the deep revision of the mathematical apparatus for electrodynamics, called to the creation of the mathematical means of the more adequate description of passage from one inertial reference system to another. Approach to precisely this development of the mathematical apparatus for electrodynamics was proposed by A. S. Dubrovin in [10]. This approach lies within the framework the sequential revision of ideas about the space and the time with the failure of the relativistic and the passage to the new ideas, which we call gipercontinual.

The concept of time-spatial gipercontinuum is introduced in [11] as a result the joint study of the algebraic and geometric structures of the commutative algebras with one, elements of which are the functions of sine waves. The hypothesis of gipercontinuum (about the hierarchical gipercontinual structure of world physical space-time) is starting point of scientific studies, directed toward the generalization of ideas about the structure of space and time in the course of passage from the contemporary quantum scientific paradigm to the new system, that simultaneously structurally connecting up its framework continuity and the discretion, dynamicity and static character, and also globality and the locality [5, 6, 12]. The hierarchical quality of gipercontinuum limits the applicability of the conventional principle of geometrization in physics and the connected with it ideas of symmetry in the geometry due to the introduction into theoretical physics of the ideas of hierarchical quality [7,13], effectiveness of which have approved we with the creation of the standard model of the protected automated system (EMZAS) and the mathematical apparatus of the EMZAS- networks [14].

In [10] is proposed new approach to the development of the mathematical apparatus for electrodynamics in the direction of the more adequate description of passage from one inertial reference system to another on the basis of giperkontinualnykh ideas about the space and in the time due to the improvement of differential calculus of the field functions under the assumption of their dependence on the speed of the motion of observer. Let us accept for the basis this approach.

III. MATHEMATICAL APPARATUS FOR THE TRANSCOORDINATE ELECTRODYNAMICS

Two inertial reference systems with the time united for them will examine $t \in \mathbb{R}$. one of them (with the system of rectangular Cartesian space coordinates $OXYZ$) let us name laboratory (not

shtrikhovannoy) and we will interpret it as relatively fixed. The second (with the system of rectangular Cartesian space coordinates $O'X'Y'Z'$) let us name substantive (shtrikhovannoy) and we will interpret it as connected with the certain moving real or imaginary medium. Let us assume that with $t = 0$ the system of space coordinates of both frame of references they coincide.

Let us introduce the indices $\alpha = \overline{1,3}$ $\beta = \overline{1,3}$.

Coordinates along the axes $OX, OY, OZ, O'X', O'Y', O'Z'$ we will assign by variables x^α and x'^α respectively.

Unit vectors along the axes OX and $O'X'$, the axes OY and $O'Y'$, the axes $OZ, O'Z'$ let us designate through $\mathbf{e}_\beta = \begin{pmatrix} e_\beta^\alpha \end{pmatrix}$, moreover

$e_\beta^\alpha = \delta_{\alpha\beta}$, where $\delta_{\alpha\beta}$ – Kronecker's symbol.

Through $\mathbf{v} = \begin{pmatrix} v^\alpha \end{pmatrix}$ let us designate the velocity vector of the motion of substantive frame of reference relative to laboratory and the module of this vector.

Directing a unit vector $\mathbf{e}_1 = \mathbf{v}$, we lengthwise have:

$\mathbf{v} = v\mathbf{e}_1 = \begin{pmatrix} v^\alpha \end{pmatrix}$, $v^\alpha = v\delta_{\alpha 1}$. Event in the data two

frame of references takes the form $\mathbf{x} = (\mathbf{r}, t) = \begin{pmatrix} x^\alpha, t \end{pmatrix}$; $\mathbf{x}' = (\mathbf{r}', t) = \begin{pmatrix} x'^\alpha, t \end{pmatrix}$, where $\mathbf{r} = \begin{pmatrix} x^\alpha \end{pmatrix}$, $\mathbf{r}' = \begin{pmatrix} x'^\alpha \end{pmatrix}$ – the radius-vectors. We will consider that the physical equivalence of events $\mathbf{x} = \mathbf{x}'$ indicates the validity of the Galileo conversion

$$\mathbf{r} = \mathbf{r}' + t\mathbf{v}, \tag{1}$$

or, otherwise, substituting vector idea by the component,

$$x^\alpha = x'^\alpha + tv\delta_{\alpha 1} \tag{2}$$

Classical physical field is described in the laboratory and substantive frame of references by its field functions $\Phi(\mathbf{r}, t)$ and $\Phi'(\mathbf{v}, \mathbf{r}', t)$, moreover $\Phi'(\mathbf{0}, \mathbf{r}', t) = \Phi(\mathbf{r}', t)$, and equality $\mathbf{v} = \mathbf{0}$ indicates $v^\alpha = 0$. Their values are called field variables. For

pour on different physical nature they can be suitable the different mathematical ideas of field functions, so that field variables can be, for example, scalar or vector with the material or complex values of their most variable or vector components. If in the role of this field electric field comes out, then in this role can come out the functions of its tension $\mathbf{E} = \Phi(\mathbf{r}, t)$,

$\mathbf{E}' = \Phi'(\mathbf{v}, \mathbf{r}', t)$, and in the case of magnetic field we have functions of the magnetic induction $\mathbf{B} = \Phi(\mathbf{r}, t)$,

$$\mathbf{B}' = \Phi'(\mathbf{v}, \mathbf{r}', t).$$



In the classical nonrelativistic field theory it is considered that the equality occurs

$$\Phi(\mathbf{r}' + t\mathbf{v}, t) = \Phi'(\mathbf{v}, \mathbf{r}', t), \tag{3}$$

mathematically expressing the physical concept of the invariance of field relative to the speed of the motion of observer. In the theory of relativity (3) no longer it is carried out, but the Lorentz conversions are used instead of the Galileo conversions. But this not invariance of field does not have fundamental, that not connected with the geometry of the space-time of physical nature, but it occurs simply the consequence of the effects of the reduction of lengths and time dilation in the moving frame of references. The proposed by us gipercontinual ideas about the space and the time [11] provide for the great possibilities of the invariance of various physical processes relative to various transformation groups of coordinates with the fact that special role in time-spatial gipercontinuum play the

$$\frac{d\Phi(\mathbf{r}', t)}{dt} = \frac{d\Phi(\mathbf{r}' + t\mathbf{v}, t)}{dt} = \lim_{\Delta t \rightarrow 0} \frac{\Phi(\mathbf{r}' + (t + \Delta t)\mathbf{v}, t + \Delta t) - \Phi(\mathbf{r}' + t\mathbf{v}, t)}{\Delta t} \tag{4}$$

But it is possible to examine also the derivative (let us name its Galileo derivative), whose arguments will

$$\frac{\partial' \Phi}{\partial t}(\mathbf{v}, \mathbf{r}', t) = \frac{d\Phi(\mathbf{r}' + t\mathbf{v}, t)}{dt} = \lim_{\Delta t \rightarrow 0} \frac{\Phi(\mathbf{r}' + (t + \Delta t)\mathbf{v}, t + \Delta t) - \Phi(\mathbf{r}' + t\mathbf{v}, t)}{\Delta t} \tag{5}$$

If the arguments of the Lagrange and Galileo derivatives are connected with equality (1), that their corresponding values are equal and are decomposed

$$\frac{\partial' \Phi}{\partial t}(\mathbf{v}, \mathbf{r}', t) = \frac{d\Phi(\mathbf{r}, t)}{dt} = \frac{\partial \Phi(\mathbf{r}' + t\mathbf{v}, t)}{\partial t} + (\mathbf{v} \cdot \nabla)\Phi(\mathbf{r}' + t\mathbf{v}, t) \tag{6}$$

Let us explain a difference in the physical sense of the Lagrange and Galilean derivatives of field function. Lagrange's derivative (4) is complete time derivative of the function of field in the laboratory frame of reference, measured at the point of space, which in the laboratory frame of reference at the moment of time t has a radius-vector \mathbf{r} , determined by the equality (1). But Galileo derivative (5) is complete time derivative

$$\frac{d^1 \Phi(\mathbf{r}, t)}{dt^1} = \frac{d\Phi(\mathbf{r}, t)}{dt}; \quad \frac{d^{n+1} \Phi(\mathbf{r}, t)}{dt^{n+1}} = \frac{d}{dt} \frac{d^n \Phi(\mathbf{r}, t)}{dt^n};$$

$$\frac{\partial'^1 \Phi}{\partial t^1}(\mathbf{v}, \mathbf{r}', t) = \frac{\partial' \Phi}{\partial t}(\mathbf{v}, \mathbf{r}', t); \quad \frac{\partial'^n \Phi}{\partial t^n}(\mathbf{v}, \mathbf{r}', t) = \frac{d^n \Phi(\mathbf{r}, t)}{dt^n}.$$

.Within the framework concepts of the invariance of field relative to the speed of the motion of observer, i.e., with fulfillment condition (3), we have:

$$\frac{\partial' \Phi}{\partial t}(\mathbf{v}, \mathbf{r}', t) = \frac{d\Phi(\mathbf{r}' + t\mathbf{v}, t)}{dt} = \frac{d\Phi'(\mathbf{v}, \mathbf{r}', t)}{dt} = \frac{\partial \Phi'(\mathbf{v}, \mathbf{r}', t)}{\partial t} \tag{7}$$

Galileo conversions (1), since they in this case they treat as the level Lorentz conversions of infinitely high level and, thus, they make it possible in a united manner to synchronize all events in all separate continua, hierarchically structure into united gipercontinuum. Natural to consider that in giperkontinuum the field also not is invariant relative to the speed of the motion of observer, but to explain this by the already fundamental properties of field, not connected with the geometry of separate continua.

A rises the question about the possible versions of complete differentiation concerning the time of field function in the laboratory frame of reference $\Phi(\mathbf{r}, t)$, of that produced depending on substantive frame of reference. In fluid mechanics and classical mechanics widely is used the derivative of Lagrange (the substantial derivative), which has the same arguments as the initial field function:

coincide with the arguments of field function no longer in the laboratory, but in the substantive frame of reference:

into one and the same sum of quotient on the time and the convective derivative of field function in the laboratory frame of reference:

of the function of field in the laboratory frame of reference, measured at the point of space, which in the substantive frame of reference has a radius- vector \mathbf{r}' . The concepts of Lagrange and Galilean derivatives (4)-(6) naturally are generalized to the case derivative of higher order ($n = \overline{1, \infty}$):

i.e., Galileo derivative of field in the laboratory frame of reference is not distinguished from the particular time derivative of the function of field in the substantive frame of reference. Therefore introduction within the framework to this concept of the Galileo derivative as some new mathematical object with its independent physical sense, is superfluous. However, within the framework relativistic ideas examination by Galileo's derivative is empty because of the emptiness of very Galileo conversions (in contrast to the Lorentz conversions). But giperkontinual ideas about the space and the time make Galilean derived completely by that claimed, and equality (7) – to false.

This view on the space, the period and the electromagnetic field in conjunction with the application of Galileo's derivative leads to the new, trans-coordinate formulation of the electrodynamics [10]. It generalizes the conventional formulation of Hertz- Heaviside, which will be examined below.

IV. MATHEMATICAL MODELS OF THE ELECTROMAGNETIC FIELD

Electromagnetic field in the isotropic homogeneous medium without the dispersion is described in the laboratory and substantive frame of references by its variables (tension of electric field $\mathbf{E} = (E^\alpha)$, $\mathbf{E}' = (E'^\alpha)$ and magnetic induction $\mathbf{B} = (B^\alpha)$, $\mathbf{B}' = (B'^\alpha)$), by constants (electrical ϵ_0 and magnetic μ_0), and also expressed as them speed of light in the vacuum $c = 1/\sqrt{\epsilon_0\mu_0}$, by the

$$\oint_s \mathbf{E} \cdot ds = Q/(\epsilon\epsilon_0); \oint_s \mathbf{B} \cdot ds = 0; \oint_l \mathbf{E} \cdot dl = -\frac{d}{dt} \int_s \mathbf{B} \cdot ds; \frac{c^2}{\epsilon\mu} \oint_l \mathbf{B} \cdot dl = \frac{I}{\epsilon\epsilon_0} + \frac{d}{dt} \int_s \mathbf{E} \cdot ds, \quad (10)$$

where s , l – the arbitrary two-dimensional closed (for the first two equations) or open (for the second two equations) surface and its limiting locked outline, which not not compulsorily coincides with the electric circuit. If we on Wednesday put the even additional condition of the absence of free charges and currents, then last two equations (10) will take the form:

$$\oint_l \mathbf{E} \cdot dl = -\frac{d}{dt} \int_s \mathbf{B} \cdot ds, \quad \oint_l \mathbf{B} \cdot dl = \frac{\epsilon\mu}{c^2} \frac{d}{dt} \int_s \mathbf{E} \cdot ds. \quad (11)$$

They are the integral form of the law of the induction of Faraday and circulation theorem of magnetic field in the laboratory frame of reference for this special case of medium.

These two laws take the mutually symmetrical form with an accuracy to of scalar factor, by virtue of which their analysis it is identical. Let us examine the first law in more detail, for example. In Faraday

parameters (dielectric and magnetic constant ϵ and μ , and also the density of strange electric charge ρ , ρ' the electric current density of conductivity $\mathbf{j} = (j^\alpha)$, $\mathbf{j}' = (j'^\alpha)$, electric charge Q , Q' , electric current I , I'), by field functions $\mathbf{E} = \mathbf{E}(\mathbf{r}, t) = (E^\alpha(\mathbf{r}, t))$, $\mathbf{B} = \mathbf{B}(\mathbf{r}, t) = (B^\alpha(\mathbf{r}, t))$, $\mathbf{E}' = \mathbf{E}'(\mathbf{v}, \mathbf{r}', t) = (E'^\alpha(\mathbf{v}, \mathbf{r}', t))$, $\mathbf{B}' = \mathbf{B}'(\mathbf{v}, \mathbf{r}', t) = (B'^\alpha(\mathbf{v}, \mathbf{r}', t))$, moreover $\mathbf{E}'(0, \mathbf{r}', t) = \mathbf{E}(\mathbf{r}', t)$; $\mathbf{B}'(0, \mathbf{r}', t) = \mathbf{B}(\mathbf{v}, \mathbf{r}', t)$. (8)

In the classical nonrelativistic electrodynamics it is relied:

$$\begin{aligned} \mathbf{E}(\mathbf{r}' + t\mathbf{v}\mathbf{e}_1, t) &= \mathbf{E}'(\mathbf{v}, \mathbf{r}', t); \\ \mathbf{B}(\mathbf{r}' + t\mathbf{v}\mathbf{e}_1, t) &= \mathbf{B}'(\mathbf{v}, \mathbf{r}', t), \end{aligned} \quad (9)$$

what is the application of a general formula (3) of the invariance of field relative to the speed of the motion of observer for the case of electromagnetic field. The proposed by us giperkontinualnye ideas about the space and the time [11] exceed the scope of this concept, but is explained nature of this not invariance not by the geometry of united space-time similar to the theory of relativity, but by the fundamental properties of field.

The integral form of Maxwell equations in the idea of Hertz-Heaviside with the above-indicated conditions (isotropy, the uniformity of medium, the absence in it of dispersion) is the following system of four integral equations of the electrodynamics:

experiences it is experimentally established that in the outline the identical currents appear regardless of the fact, this outline relative to the current carrying outline does move or it rests, and the current carrying outline moves, provided their relative motion in both cases was identical (Galilean invariance of Faraday law). Therefore the flow through the outline can change as a result of a change of the magnetic field with time, and the position of its boundary also because with the displacement of outline changes [15]. The corresponding generalization of laws (11) to the case of the outline, which moves in the laboratory and which is rested in the substantive frame of reference, takes the form:

$$\oint_l \mathbf{E}' \cdot dl = -\frac{d}{dt} \int_s \mathbf{B} \cdot ds, \quad \oint_l \mathbf{B}' \cdot dl = \frac{\epsilon\mu}{c^2} \frac{d}{dt} \int_s \mathbf{E} \cdot ds. \quad (12)$$

where \mathbf{E}' , \mathbf{B}' are described fields in the element dl in the substantive frame of reference, i.e., in such inertial

reference system, in which dl it rests; specifically, such electric field causes the appearance of a current in the case of the presence of real electric circuit in this place. Equations (12) are completely interesting and uncommon from a mathematical point of view, since they mutually connect field variables in the different inertial reference systems (let us name such equations trans-coordinate). Specifically, the use of trans-coordinate equations makes it possible to adequately describe physical fields in giperkontinuume. At the same time in this case the discussion deals not simply about the trans-coordinateawn of equations (12), and with their global trans-coordinateawn, ensured by use by the Galilean derivative (connected by them inertial reference

systems they can move relative to each other with the arbitrary speed, and not compulsorily with infinitely small).

Returning to the system of equations (10), it is possible to establish that the region of its applicability is limited by the requirement of the state of rest of outline l in the laboratory frame of reference. If we remove this limitation, after requiring only the states of rest of outline l in the substantive frame of reference, then will come out the known idea of Maxwell equations (we we call his trans-coordinate 10), integral form of which will be in it the system of the generalizing (10) four integral equations of the electrodynamics of the moving media:

$$\oint_s \mathbf{E} \cdot d\mathbf{s} = Q/(\epsilon\epsilon_0); \oint_s \mathbf{B} \cdot d\mathbf{s} = 0; \oint_l \mathbf{E}' \cdot d\mathbf{l} = -\frac{d}{dt} \int_s \mathbf{B} \cdot d\mathbf{s}; \frac{c}{\epsilon\mu} \oint_l \mathbf{B}' \cdot d\mathbf{l} = \frac{I'}{\epsilon\epsilon_0} + \frac{d}{dt} \int_s \mathbf{E} \cdot d\mathbf{s} \quad (13)$$

If the transcoordinate idea of the equations of Maxwell (both in that examined by integral and in that examined lower than the differential forms) to interpret in the context of the description of electromagnetic field in time-spatial gipercontinuum, then it is necessary to consider that the equalities (8) are always carried out, but (9) – in the general case no.

Equations (12) (13) are known in the classical electrodynamics [15, 16]. Arises question, as to pass

$$\nabla \cdot \mathbf{E} = \rho/(\epsilon\epsilon_0); \nabla \cdot \mathbf{B} = 0; \nabla \times \mathbf{E} = -\partial\mathbf{B}/\partial t; \nabla \times \mathbf{B} = \mu\mu_0\mathbf{j} + \left(\epsilon\mu/c^2\right)(\partial\mathbf{E}/\partial t) \quad (14)$$

Equations (14) traditionally successfully are used in the electrodynamics, but, as it will be shown below, they have essential deficiency – the region of their applicability it is limited by the case of agreeing the laboratory and substantive frame of references ($v = 0$), i.e. these equations are deprived of the mathematical means of the adequate description of passage from one inertial reference system to another, completely tying process to one (laboratory) frame of reference.

In [15] based on the example of Faraday law is formulated the following approach to the passage from the integral to the differential form of equations electrodynamics: "Faraday law can be written down also in the differential form, if we use ourselves the Stokes' theorem and to consider outline as that being resting in the selected frame of reference (so that \mathbf{E} and \mathbf{B} they would be determined in one and the same frame of reference)". This approach answers the concept of the invariance of physical field relative to the speed of the motion of observer, assuming simple failure of the trans-coordinateawn of equations by means of the application (9). But, rejecting this concept, it is necessary to reject this approach. Thus, the differential form of the corresponding equations must be the same trans-coordinate as integral (12), (13).

from the equations in the integral form (12) and (13) to the corresponding to equations in the differential form adequate of physical reality by means.

The differential form of Maxwell equations in the idea of Hertz- Heaviside is following system of four of those corresponding to the integral equations (10) of the differential equations of electrodynamics, which relate to the laboratory frame of reference:

In accordance with the given traditional approach, in [16] is introduced the operation of differentiation with respect to time in the moving (substantive) frame of reference, designated there through $\partial'/\partial t$. In this case it is secretly assumed that

at the point of space, which in the substantive frame of reference has a radius-vector \mathbf{r}' , measurement by field variable in the laboratory frame of reference equivalent to its measurement in the same substantive frame of reference. But these measurements are not equivalent out of the concept of the invariance of physical field relative to the speed of the motion of observer. Therefore measurement must be limited by laboratory frame of reference, not perenosya its results for the substantive. Thus, we come to the Galileo derivative (5), of the electrodynamics in the differential form leaving equations globally transcoordinate.

Unknown globally transcoordinate differential equations of electrodynamics, which correspond to integral equations (12) and which use the Galileo derivative:

$$\nabla \times \mathbf{E}' = -\frac{\partial'\mathbf{B}}{\partial t}, \nabla \times \mathbf{B}' = \frac{\epsilon\mu}{c^2} \frac{\partial'\mathbf{E}}{\partial t} \quad (15)$$

They are generalization to the case of the noncoincidence of the laboratory and substantive frame of references ($\mathbf{v} \neq \mathbf{0}$) of the known differential equations of Maxwell

$$\nabla \times \mathbf{E} = -\frac{\partial \mathbf{B}}{\partial t}, \nabla \times \mathbf{B} = \frac{\varepsilon\mu}{c^2} \frac{\partial \mathbf{E}}{\partial t}. \quad (16)$$

The differential form of Maxwell equations in the trans-coordinate idea for the case of isotropic, homogeneous medium without the dispersion is the following system of four new globally trans-coordinate differential equations of the electrodynamics:

$$\frac{\partial \mathbf{E}}{\partial t}(\mathbf{v}, \mathbf{r}', t) = \frac{\partial \mathbf{E}(\mathbf{r}' + t\mathbf{v}\mathbf{e}_1, t)}{\partial t} + (\mathbf{v}\mathbf{e}_1 \cdot \nabla) \mathbf{E}(\mathbf{r}' + t\mathbf{v}\mathbf{e}_1, t) \quad (19)$$

$$\frac{\partial \mathbf{B}}{\partial t}(\mathbf{v}, \mathbf{r}', t) = \frac{\partial \mathbf{B}(\mathbf{r}' + t\mathbf{v}\mathbf{e}_1, t)}{\partial t} + (\mathbf{v}\mathbf{e}_1 \cdot \nabla) \mathbf{B}(\mathbf{r}' + t\mathbf{v}\mathbf{e}_1, t) \quad (20)$$

With $\mathbf{v} = \mathbf{0}$ (17)-(18) it passes in (14).

In the particular case the absences of free charges and currents of equation (17)-(18) will take the form:

$$\nabla \cdot \mathbf{E}(\mathbf{r}, t) = \frac{\rho(\mathbf{r}, t)}{\varepsilon\varepsilon_0}; \nabla \cdot \mathbf{B}(\mathbf{r}, t) = 0; \quad (17)$$

$$\nabla \times \mathbf{E}'(\mathbf{v}, \mathbf{r}', t) = -\frac{\partial \mathbf{B}}{\partial t}(\mathbf{v}, \mathbf{r}', t);$$

$$\nabla \times \mathbf{B}'(\mathbf{v}, \mathbf{r}', t) = \mu\mu_0 \mathbf{j}'(\mathbf{v}, \mathbf{r}', t) + \frac{\varepsilon\mu}{c^2} \frac{\partial \mathbf{E}}{\partial t}(\mathbf{v}, \mathbf{r}', t), \quad (18)$$

where $\partial \mathbf{E}'/\partial t$, $\partial \mathbf{B}'/\partial t$ – the Galileo derivatives of field functions, expressed as particular time derivatives and convective derivatives of the same field functions in the laboratory frame of reference by the following equalities:

$$\nabla \cdot \mathbf{E}(\mathbf{r}, t) = 0; \nabla \cdot \mathbf{B}(\mathbf{r}, t) = 0; \quad (21)$$

$$\nabla \times \mathbf{E}'(\mathbf{v}, \mathbf{r}', t) = -\frac{\partial \mathbf{B}}{\partial t}(\mathbf{v}, \mathbf{r}', t) \quad \nabla \times \mathbf{B}'(\mathbf{v}, \mathbf{r}', t) = \frac{\varepsilon\mu}{c^2} \frac{\partial \mathbf{E}}{\partial t}(\mathbf{v}, \mathbf{r}', t) \quad (22)$$

With $\mathbf{v} = \mathbf{0}$ (21)-(22) it passes into the well-known system of equations of Maxwell:

$$\nabla \cdot \mathbf{E}(\mathbf{r}, t) = 0; \nabla \cdot \mathbf{B}(\mathbf{r}, t) = 0; \nabla \times \mathbf{E}(\mathbf{r}, t) = -\frac{\partial \mathbf{B}(\mathbf{r}, t)}{\partial t}; \nabla \times \mathbf{B}(\mathbf{r}, t) = \frac{\varepsilon\mu}{c^2} \frac{\partial \mathbf{E}(\mathbf{r}, t)}{\partial t}. \quad (23)$$

By the vector product of nabla to both parts of the equations (16) with their mutual substitution into each other obtains the known wave differential equations

$$c^2 \nabla^2 \mathbf{E} = \varepsilon\mu \frac{\partial^2 \mathbf{E}}{\partial t^2}, c^2 \nabla^2 \mathbf{B} = \varepsilon\mu \frac{\partial^2 \mathbf{B}}{\partial t^2} \quad (24)$$

The absence of trans-coordinateawn is their drawback, they are valid only in the case of agreeing the laboratory and substantive frame of references ($\mathbf{v} = \mathbf{0}$). It is analogous, i.e., by the vector product of nabla to both parts of the equations (15) with their mutual substitution into each other, we will obtain the new equations of electrodynamics – the globally trans-coordinate wave differential equations, which use

Galilean derivative of field functions and generalizing equations (24) in the case $\mathbf{v} \neq \mathbf{0}$:

$$c^2 \nabla'^2 \mathbf{E}' = \varepsilon\mu \frac{\partial'^2 \mathbf{E}}{\partial t'^2}, c^2 \nabla'^2 \mathbf{B}' = \varepsilon\mu \frac{\partial'^2 \mathbf{B}}{\partial t'^2}. \quad (25)$$

We investigate in more detail the equation of form (25) in connection with to arbitrary field functions $\Phi(x, t)$, also, $\Phi'(\mathbf{v}, x', t)$ for the case of plane wave with the wave vector, collinear to vector $\mathbf{v} = (v, 0, 0)$ and to axes OX , $O'X'$, coordinates along which are assigned by the variables x , x' . In this case the equation proves to be one-dimensional, and field functions – scalar:

$$c^2 \frac{\partial^2}{\partial x'^2} \Phi'(\mathbf{v}, x', t) = \varepsilon\mu \frac{\partial'^2 \Phi}{\partial t'^2}(\mathbf{v}, x', t) = \varepsilon\mu \frac{d^2}{dt^2} \Phi(x' + vt, t) \quad (26)$$

If we differentiate in the right side (26), this equation of signs the form:

$$\frac{c^2}{\varepsilon\mu} \frac{\partial^2}{\partial x'^2} \Phi'(\mathbf{v}, x', t) = \left(\frac{\partial^2}{\partial t^2} + 2v \frac{\partial^2}{\partial t \partial x} + v^2 \frac{\partial^2}{\partial x^2} \right) \Phi(x' + vt, t) = \left(\frac{\partial}{\partial t} + v \frac{\partial}{\partial x} \right)^2 \Phi(x' + vt, t) \quad (27)$$

With $v = 0$ (26) (27) it degenerates into the one-dimensional version of the wave equation of the form (24):

$$c^2 \frac{\partial^2}{\partial x^2} \Phi(x, t) = \varepsilon\mu \frac{\partial^2}{\partial t^2} \Phi(x, t). \quad (28)$$

Any solution (28) is determined by the proper superposition of the simple harmonic waves

$$\Phi(x, t) = A \cos(\omega t - k_x x + \varphi) \quad (29)$$

$k'_x(v)$, $\varphi'(v)$:

$$\Phi'(v, x', t) = A'(v) \cos(\omega'(v)t - k'_x(v)x' + \varphi'(v)) \quad (30)$$

$\Phi'(0, x', t) = \Phi(x', t)$, $A'(0) = A$, $\omega'(0) = \omega$, $k'_x(0) = k_x$, $\varphi'(0) = \varphi$. Let us substitute (29)-(30) in

$$c^2 k_x'^2(v) A'(v) \cos(\omega'(v)t - k'_x(v)x' + \varphi'(v)) = \varepsilon\mu (\omega - k_x v)^2 A \cos(\omega t - k_x(x' + vt) + \varphi). \quad (31)$$

Equalizing the similar parameters of wave on the left side (31) and in the right, we have:

$$A'(v) = \left(\operatorname{sgn} k_x - \frac{\sqrt{\varepsilon\mu}}{c} v \right)^2 A , \quad \omega'(v) = |\omega - k_x v| = \left| 1 - \frac{\sqrt{\varepsilon\mu}}{c} v \operatorname{sgn} k_x \right| \omega \quad (32)$$

$$k'_x(v) = k_x \operatorname{sgn}(\omega - k_x v) , \quad k'(v) = |k'_x(v)| = k , \quad \varphi'(v) = \varphi \operatorname{sgn}(\omega - k_x v) , \quad |\varphi'(v)| = |\varphi|. \quad (33)$$

Thus, upon transfer from the laboratory to the substantive frame of reference change amplitude and frequency (32) of simple harmonic wave, and its wave number and module of initial phase (33) remain constant. In this case the frequency changes in such a

with the approximate values of the parameters $A \geq 0$, $\omega > 0$, $k_x \neq 0$, $\varphi \in \mathbb{R}$ – amplitude, angular frequency, the projection of wave vector on the axis OX and the initial phase of wave. In this case all waves (29) must have one and the same phase speed $\omega/k = c/\sqrt{\varepsilon\mu}$, where $k = |k_x|$ – wave number. We will search for function $\Phi'(v, x', t)$, satisfying (26)-(29), also in the form of simple harmonic wave, but with those depending on v by the parameters $A'(v)$, $\omega'(v)$

way that phase wave velocity in the substantive frame of reference is obtained according to the classical summation rule of speeds from its phase speed in the laboratory frame of reference and speed of substantive frame of reference relative to the laboratory:

$$\omega'(v)/k'_x(v) = \omega'(v)/k_x = \omega/k_x - v , \quad \omega'(v)/k'(v) = |\omega/k - v \operatorname{sgn} k_x| = \left| c/\sqrt{\varepsilon\mu} - v \operatorname{sgn} k_x \right|. \quad (34)$$

From (32)-(34) it is evident that if the vector of phase wave velocity in the laboratory frame of reference coincides with the velocity vector of substantive frame of reference in it ($k_x > 0$, $v = \omega/k$), that in the substantive frame of reference wave generally disappears ($A'(v) = 0$). Thus, in contrast to the theory of relativity, in the theory of gipercontinuum this wave always can be destroyed by the suitable selection of frame of reference. But if relative to laboratory frame of

reference substantial frame of reference outdistances wave, then upon transfer from the laboratory frame of reference to the substantive the direction of propagation of wave changes by the opposite. If in the laboratory frame of reference wave is propagated in the positive direction, then upon transfer into the substantive it will satisfy wave equation (35), while if in the negative, then to the equation (36):

$$\left(\frac{c}{\sqrt{\varepsilon\mu}} - v \right)^2 \partial^2 \Phi'(v, x', t) / \partial x'^2 = \partial^2 \Phi'(v, x', t) / \partial t^2 \quad (35)$$

$$\left(\frac{c}{\sqrt{\varepsilon\mu}} + v \right)^2 \partial^2 \Phi'(v, x', t) / \partial x'^2 = \partial^2 \Phi'(v, x', t) / \partial t^2 \quad (36)$$

The selection of inertial reference system to the role of laboratory is, generally speaking, conditional. Thus, substantial frame of reference it is possible in turn to accept for the laboratory, and in the role of substantial

to examine certain by third (twice prime) inertial reference system with that directed to the same side, that also OX , $O'X'$, by attitude reference $O''X''$, the coordinate along which is assigned by the variable

x'' . Let, for example, the point O'' move in the positive direction of axis $O'X'$ with the speed Δv . Wave in the new laboratory and substantive frame of references will have an identical wave number and a module of initial phase and will be described by field functions

$$\left(\frac{c}{\sqrt{\varepsilon\mu}} - (v + \Delta v)\right)^2 \partial^2 \Phi'(v + \Delta v, x'', t) / \partial x''^2 = \partial^2 \Phi'(v + \Delta v, x'', t) / \partial t^2 \tag{37}$$

$$\left(\frac{c}{\sqrt{\varepsilon\mu}} + (v + \Delta v)\right)^2 \partial^2 \Phi'(v + \Delta v, x'', t) / \partial x''^2 = \partial^2 \Phi'(v + \Delta v, x'', t) / \partial t^2 \tag{38}$$

For (37) the role of equalities (32), (33) play the following transformations of the parameters of the wave:

$$A''(v + \Delta v) = \left(\operatorname{sgn} k'_x(v) - \frac{\sqrt{\varepsilon\mu} \cdot \Delta v}{c - \sqrt{\varepsilon\mu} \cdot v} \right)^2 A'(v), \quad \omega''(v + \Delta v) = |\omega'(v) - k'_x(v)\Delta v|, \tag{39}$$

$$k''_x(v + \Delta v) = k'_x(v) \operatorname{sgn}(\omega'(v) - k'_x(v)\Delta v), \quad \varphi''(v + \Delta v) = \varphi'(v) \operatorname{sgn}(\omega'(v) - k'_x(v)\Delta v) \tag{40}$$

For (38) the corresponding (39)-(40) conversions of the parameters are determined analogously.

Sequential passage from not shtrikhovannoy to shtrikhovannoy and is further to the twice shtrikhovannoy frame of reference equivalent to direct passage from not shtrikhovannoy to twice shtrikhovannoy. For example, which is obtained also upon direct transfer to the twice

$\Phi'(v, x', t)$ and $\Phi'(v + \Delta v, x'', t)$ respectively. The role of equation (28) plays (35) or (36), the role of the function of wave (29) – function (30), while the role of equations (35), (36) – the following wave equations:

with $\operatorname{sgn} k'_x(v) = \operatorname{sgn} k_x = 1$ from (32), (39) it is possible to obtain

$$A''(v + \Delta v) = \left(1 - \sqrt{\varepsilon\mu} (v + \Delta v) / c\right)^2 A, \tag{41}$$

shtrikhovannoy frame of reference, since (41) it is obtained from (32) by replacement v on $v + \Delta v$. In this case the role of equation (27) plays

$$\left(\frac{c}{\sqrt{\varepsilon\mu}} - v\right)^2 \frac{\partial^2 \Phi'(v + \Delta v, x'', t)}{\partial x''^2} = \frac{\partial^2 \Phi'(v, x'' + \Delta vt, t)}{\partial t^2} + \left(2\Delta v \frac{\partial^2}{\partial t \partial x'} + \Delta v^2 \frac{\partial^2}{\partial x'^2}\right) \Phi'(v, x'' + \Delta vt, t). \tag{42}$$

For the derivatives of arbitrary n of order $\partial^n \Phi'(v + \Delta v, x'', t) / \partial x''^n$ $\partial^n \Phi'(v, x', t) / \partial x'^n$ it is possible to use a united designation $\partial^n \Phi'(v + \Delta v, x, t) / \partial x^n$ and $\partial^n \Phi'(v, x, t) / \partial x^n$

$n = \overline{1, \infty}$), respectively indicating simply derived on the second argument. In accordance with this, after substitution (35) in (42) we will obtain:

$$\left(\frac{c}{\sqrt{\varepsilon\mu}} - v\right)^2 \frac{\partial^2}{\partial x^2} \left(\frac{\Phi'(v + \Delta v, x, t) - \Phi'(v, x + \Delta vt, t)}{\Delta v} \right) = \left(2 \frac{\partial^2}{\partial t \partial x} + \Delta v \frac{\partial^2}{\partial x^2}\right) \Phi'(v, x + \Delta vt, t) \tag{43}$$

Let $\Delta v \rightarrow 0$. Let us introduce one additional new derivative, which let us name trans-coordinate, and which in the case of the one-dimensional system of space coordinates takes the form:

$$\frac{\partial' \Phi'(v, x, t)}{\partial' v} = \lim_{\Delta v \rightarrow 0} \frac{\Phi'(v + \Delta v, x, t) - \Phi'(v, x + \Delta vt, t)}{\Delta v}. \tag{44}$$

In the determination (44) of value $\Phi'(v, x + \Delta vt, t)$ $\Phi'(v + \Delta v, x, t)$ is described physical field at one and the same point of space, but in the different frame of references (shtrikhovannoy and moving relative to it with speed Δv twice prime respectively). Within the framework they are equal to the

concept of the invariance of field relative to the speed of the motion of observer:

$$\Phi'(v, x + \Delta vt, t) = \Phi'(v + \Delta v, x, t) \tag{45}$$

the equalities (3) (45) making identical physical sense, but in connection with to the different pairs of frame of references. However, out of the framework of the indicated concept upon transfer from shtrikhovannoy to the twice shtrikhovannoy frame of reference the field function at the particular point of space experiences the increase, the limit of relation of which $k \Delta v$ with $\Delta v \rightarrow 0$ gives the trans-coordinate derivative (44). It is possible to generalize it to the case of the higher orders ($n = \overline{1, \infty}$):

$$\frac{\partial'^1 \Phi'(v, x, t)}{\partial'v^1} = \frac{\partial' \Phi'(v, x, t)}{\partial'v}; \quad \frac{\partial'^{m+1} \Phi'(v, x, t)}{\partial'v^{m+1}} = \lim_{\Delta v \rightarrow 0} \frac{\frac{\partial^m \Phi'(v + \Delta v, x, t)}{\partial'v^m} - \frac{\partial^m \Phi'(v, x + \Delta vt, t)}{\partial'v^m}}{\Delta v} \quad (46)$$

Using trans-coordinate derivatives of the first two orders (46), it is possible to represent increase in

the field function of in the form corresponding partial summation of series of Taylor:

$$\Phi'(v + \Delta v, x, t) - \Phi'(v, x + \Delta vt, t) \approx \frac{\partial' \Phi'(v, x, t)}{\partial'v} \Delta v + \frac{1}{2} \frac{\partial'^2 \Phi'(v, x, t)}{\partial'v^2} \Delta v^2 \quad (47)$$

Substituting (47) in (43), equalizing between themselves members with the identical degrees Δv in the left and right sides of the received equality, fixing $\Delta v \rightarrow 0$, taking into account that the fact that in this case $\Phi'(v, x + \Delta vt, t) \rightarrow \Phi'(v, x, t)$ and by adding equality (35) in the new form of record (with the use by variable x instead of x' , we will obtain the following system of three equations:

$$\begin{cases} \left(\frac{c}{\sqrt{\epsilon\mu}} - v \right)^2 \frac{\partial^2 \Phi'(v, x, t)}{\partial x^2} = \frac{\partial^2 \Phi'(v, x', t)}{\partial t^2}, \\ \left(\frac{c}{\sqrt{\epsilon\mu}} - v \right)^2 \frac{\partial \partial' \Phi'(v, x, t)}{\partial x \partial'v} = 2 \frac{\partial \Phi'(v, x', t)}{\partial t}, \\ \left(\frac{c}{\sqrt{\epsilon\mu}} - v \right)^2 \frac{\partial'^2 \Phi'(v, x, t)}{\partial'v^2} = 2 \Phi'(v, x', t) \end{cases} \quad (48)$$

System of equations (48) can be written down in following that indexed on α the form:

$$\left(\left(\frac{c}{\sqrt{\epsilon\mu}} - v \right)^2 \frac{\partial^{2-\alpha} \partial'^\alpha}{\partial x^{2-\alpha} \partial'v^\alpha} - 2^{\text{sgn } \alpha} \frac{\partial^{2-\alpha}}{\partial t^{2-\alpha}} \right) \Phi'(v, x', t) = 0, \quad \alpha = \overline{0, 2} \quad (49)$$

$$\otimes \Phi'(v, x', t) = 0 \quad (50)$$

or in the operator form

$$\text{where } \otimes = (\otimes^\alpha); \quad \otimes^\alpha = \left(\left(\frac{c}{\sqrt{\epsilon\mu}} - v \right)^2 \frac{\partial^{2-\alpha} \partial'^\alpha}{\partial x^{2-\alpha} \partial'v^\alpha} - 2^{\text{sgn } \alpha} \frac{\partial^{2-\alpha}}{\partial t^{2-\alpha}} \right)$$

– the suitable version of the one-dimensional (case of one axis of space coordinates) differential Dubrovin operator, which generalizes d'Alembert's operator \square , who occurs one of his three (zero) components for the laboratory frame of reference, i.e., $\alpha = 0, v = 0$. Differential equation (49) or (50) is the gipercontinual one-dimensional homogeneous wave equation, which generalizes, similar to differential equation (26) or (27), the known one-dimensional homogeneous wave equation (28). The vital difference between them (26)-(27) is lies in the fact that the globally trans-coordinate form of gipercontinual wave equation, and (49)-(50) – by its locally trans-coordinate form. Local transcoordinate means that the equation connects the inertial reference systems, which move relative to each other with the infinitely low speed.

derivative reports to equation global trans-coordinate, and by trans-coordinate derivative – local.

Thus, is proposed the new approach to the development of the mathematical apparatus for electrodynamics in the direction of the more adequate description of passage from one inertial reference system to another on the basis of gipercontinual ideas about the space and in the time due to the introduction into the examination of the globally and locally trans-coordinate equations, which use new Galilean and trans-coordinate derivatives of field functions, and also the new differential of

Dubrovin operator, which generalizes d'Alembert operator. This approach leads to the reformulation of electrodynamics with the passage from the traditional formulation of Hertz-Heaviside to the new trans-coordinate. In this case immediately arise the question about what form they have conversions of electromagnetic field upon transfer from one inertial

reference system to another, and will be these conversions the Mende conversions [17].

The convective derivatives of field functions in (19)-(20) can be written down in the form:

$$(\mathbf{ve}_1 \cdot \nabla)\mathbf{E}(\mathbf{r}' + t\mathbf{ve}_1, t) = v(\nabla \cdot \mathbf{E}(\mathbf{r}' + t\mathbf{ve}_1, t))\mathbf{e}_1 - \nabla \times (\mathbf{ve}_1 \times \mathbf{E}(\mathbf{r}' + t\mathbf{ve}_1, t)) \tag{51}$$

$$(\mathbf{ve}_1 \cdot \nabla)\mathbf{B}(\mathbf{r}' + t\mathbf{ve}_1, t) = v(\nabla \cdot \mathbf{B}(\mathbf{r}' + t\mathbf{ve}_1, t))\mathbf{e}_1 - \nabla \times (\mathbf{ve}_1 \times \mathbf{B}(\mathbf{r}' + t\mathbf{ve}_1, t)) \tag{52}$$

We have in view of the first two (22) equations taking into account (1)-(2) :

$$\nabla \cdot \mathbf{E}(\mathbf{r}' + t\mathbf{ve}_1, t) = 0 ; \nabla \cdot \mathbf{B}(\mathbf{r}' + t\mathbf{ve}_1, t) = 0 . \tag{53}$$

After substituting (53) in (51)-(52), we will obtain equalities for the convective derivatives:

$$(\mathbf{ve}_1 \cdot \nabla)\mathbf{E}(\mathbf{r}' + t\mathbf{ve}_1, t) = -\nabla \times (\mathbf{ve}_1 \times \mathbf{E}(\mathbf{r}' + t\mathbf{ve}_1, t)) \tag{54}$$

$$(\mathbf{ve}_1 \cdot \nabla)\mathbf{B}(\mathbf{r}' + t\mathbf{ve}_1, t) = -\nabla \times (\mathbf{ve}_1 \times \mathbf{B}(\mathbf{r}' + t\mathbf{ve}_1, t)) . \tag{55}$$

After substitution (54)-(55) in (19)-(20) we take another form of the Galilean derivatives:

$$\frac{\partial \mathbf{E}}{\partial t}(v, \mathbf{r}', t) = \frac{\partial \mathbf{E}(\mathbf{r}' + t\mathbf{ve}_1, t)}{\partial t} - \nabla \times (\mathbf{ve}_1 \times \mathbf{E}(\mathbf{r}' + t\mathbf{ve}_1, t)) \tag{56}$$

$$\frac{\partial \mathbf{B}}{\partial t}(v, \mathbf{r}', t) = \frac{\partial \mathbf{B}(\mathbf{r}' + t\mathbf{ve}_1, t)}{\partial t} - \nabla \times (\mathbf{ve}_1 \times \mathbf{B}(\mathbf{r}' + t\mathbf{ve}_1, t)) \tag{57}$$

The substitution of Galilean derivatives (56)-(57) into the last two equalities (22) gives:

$$\nabla \times \mathbf{E}'(v, \mathbf{r}', t) = -\partial \mathbf{B}(\mathbf{r}' + t\mathbf{ve}_1, t) / \partial t + \nabla \times (\mathbf{ve}_1 \times \mathbf{B}(\mathbf{r}' + t\mathbf{ve}_1, t)) , \tag{58}$$

$$\nabla \times \mathbf{B}'(v, \mathbf{r}', t) = \left(\varepsilon\mu / c^2 \right) \left(\partial \mathbf{E}(\mathbf{r}' + t\mathbf{ve}_1, t) / \partial t - \nabla \times (\mathbf{ve}_1 \times \mathbf{E}(\mathbf{r}' + t\mathbf{ve}_1, t)) \right) . \tag{59}$$

After substituting last two equations (23) in (58)-(59), we will obtain:

$$\nabla \times \mathbf{E}'(v, \mathbf{r}', t) = \nabla \times \mathbf{E}(\mathbf{r}' + t\mathbf{ve}_1, t) + \nabla \times (\mathbf{ve}_1 \times \mathbf{B}(\mathbf{r}' + t\mathbf{ve}_1, t)) , \tag{60}$$

$$\nabla \times \mathbf{B}'(v, \mathbf{r}', t) = \nabla \times \mathbf{B}(\mathbf{r}' + t\mathbf{ve}_1, t) - \left(\varepsilon\mu / c^2 \right) \nabla \times (\mathbf{ve}_1 \times \mathbf{E}(\mathbf{r}' + t\mathbf{ve}_1, t)) . \tag{61}$$

Let us omit the operation of rotor both parts of the equalities (60)-(61):

$$\mathbf{E}'(v, \mathbf{r}', t) = \mathbf{E}(\mathbf{r}' + t\mathbf{ve}_1, t) + \mathbf{ve}_1 \times \mathbf{B}(\mathbf{r}' + t\mathbf{ve}_1, t) , \tag{62}$$

$$\mathbf{B}'(v, \mathbf{r}', t) = \mathbf{B}(\mathbf{r}' + t\mathbf{ve}_1, t) - \left(\varepsilon\mu / c^2 \right) \mathbf{ve}_1 \times \mathbf{E}(\mathbf{r}' + t\mathbf{ve}_1, t) \tag{63}$$

Besides the shtrikhovannoy frame of reference, which moves relative to laboratory with speed v let us introduce also relatively mobile frame of reference – twice shtrikhovannuyu, that moves in the same direction with another speed $v + \Delta v$ relative to laboratory. Thus, the twice shtrikhovannaya frame of reference moves

with relatively shtrikhovannoy with speed Δv , the so that shtrikhovannuyu frame of reference can be accepted for the new laboratory (relatively fixed), and twice shtrikhovannuyu – for the new substantive.

Equalities (62)-(63) for them let us write down taking into account the replacement of radius-vector \mathbf{r}' on \mathbf{r}'' :

$$\mathbf{E}'(v + \Delta v, \mathbf{r}'', t) = \mathbf{E}'(v, \mathbf{r}'' + t\Delta v\mathbf{e}_1, t) + \Delta v\mathbf{e}_1 \times \mathbf{B}'(v, \mathbf{r}'' + t\Delta v\mathbf{e}_1, t) , \tag{64}$$

$$\mathbf{B}'(v + \Delta v, \mathbf{r}'', t) = \mathbf{B}'(v, \mathbf{r}'' + t\Delta v\mathbf{e}_1, t) - \left(\varepsilon\mu / c^2 \right) \Delta v\mathbf{e}_1 \times \mathbf{E}'(v, \mathbf{r}'' + t\Delta v\mathbf{e}_1, t) . \tag{65}$$

Let us write down equalities (64)-(65) in the following form:

$$\frac{\mathbf{E}'(v + \Delta v, \mathbf{r}'', t) - \mathbf{E}'(v, \mathbf{r}'' + t\Delta v \mathbf{e}_1, t)}{\Delta v} = \mathbf{e}_1 \times \mathbf{B}'(v, \mathbf{r}'' + t\Delta v \mathbf{e}_1, t), \tag{66}$$

$$\frac{\mathbf{B}'(v + \Delta v, \mathbf{r}'', t) - \mathbf{B}'(v, \mathbf{r}'' + t\Delta v \mathbf{e}_1, t)}{\Delta v} = -\frac{\varepsilon\mu}{c^2} \mathbf{e}_1 \times \mathbf{E}'(v, \mathbf{r}'' + t\Delta v \mathbf{e}_1, t) \tag{67}$$

In (66)-(67) the values $\mathbf{E}'(v, \mathbf{r}'' + t\Delta v \mathbf{e}_1, t)$, $\mathbf{B}'(v, \mathbf{r}'' + t\Delta v \mathbf{e}_1, t)$, $\mathbf{E}'(v + \Delta v, \mathbf{r}'', t)$, $\mathbf{B}'(v + \Delta v, \mathbf{r}'', t)$ is described the electromagnetic field at one and the same point of space (medium), but in the

different frame of references (shtrikhovanny and by twice shtrikhovanny). Within the framework they are equal to the concept of the invariance of field relative to the speed of the motion of observer:

$$\mathbf{E}'(v, \mathbf{r}'' + t\Delta v \mathbf{e}_1, t) = \mathbf{E}'(v + \Delta v, \mathbf{r}'', t), \mathbf{B}'(v, \mathbf{r}'' + t\Delta v \mathbf{e}_1, t) = \mathbf{B}'(v + \Delta v, \mathbf{r}'', t), \tag{68}$$

the equalities (9) (68) making identical physical sense, but in connection with to the different pairs of frame of references. However, out of the framework of the indicated concept upon transfer from shtrikhovanny to the twice shtrikhovanny frame of reference the field

function at the particular point of space experiences the increase, the limit of relation of which $k \Delta v$ with $\Delta v \rightarrow 0$ gives that for the first time introduced into 10 the trans-coordinate derivative of the field function:

$$\frac{\partial' \mathbf{E}'(v, \mathbf{r}'', t)}{\partial' v} = \lim_{\Delta v \rightarrow 0} \frac{\mathbf{E}'(v + \Delta v, \mathbf{r}'', t) - \mathbf{E}'(v, \mathbf{r}'' + t\Delta v \mathbf{e}_1, t)}{\Delta v}, \tag{69}$$

$$\frac{\partial' \mathbf{B}'(v, \mathbf{r}'', t)}{\partial' v} = \lim_{\Delta v \rightarrow 0} \frac{\mathbf{B}'(v + \Delta v, \mathbf{r}'', t) - \mathbf{B}'(v, \mathbf{r}'' + t\Delta v \mathbf{e}_1, t)}{\Delta v}. \tag{70}$$

Equalities (66)-(67) with $\Delta v \rightarrow 0$ taking into account (69)-(70) after replacement \mathbf{r}'' on \mathbf{r} take the form:

$$\frac{\partial' \mathbf{E}'(v, \mathbf{r}', t)}{\partial' v} = \mathbf{e}_1 \times \mathbf{B}'(v, \mathbf{r}', t); \frac{\partial' \mathbf{B}'(v, \mathbf{r}', t)}{\partial' v} = -\frac{\varepsilon\mu}{c^2} \mathbf{e}_1 \times \mathbf{E}'(v, \mathbf{r}', t). \tag{71}$$

If equations (22) are the globally trans-coordinate differential equations of electrodynamics for the case of isotropic homogeneous medium without the dispersion in the absence of free charges and currents, then equations (71) are the locally trans-coordinate differential equations of electrodynamics for the same case. The locality of transcoordinate, ensured by use by trans-coordinate derivative, means that the connected by differential equations inertial reference systems (conditionally speaking, prime and twice prime) they move relative to each other with the infinitely low speed

Δv Equations (71) form the system, by solving which, it is possible to obtain the conversions of electromagnetic field upon transfer of one inertial reference system into another.

Let us use system of equations (71) for obtaining the conversions of electromagnetic field upon transfer from the laboratory frame of reference to the substantive.

Lowering the arguments of functions, let us write down vector products in (71) in the form:

$$\mathbf{e}_1 \times \mathbf{B}' = \mathbf{e}_1 \times (B'^1 \mathbf{e}_1 + B'^2 \mathbf{e}_2 + B'^3 \mathbf{e}_3) = B'^2 \mathbf{e}_3 - B'^3 \mathbf{e}_2 \tag{72}$$

$$\mathbf{e}_1 \times \mathbf{E}' = \mathbf{e}_1 \times (E'^1 \mathbf{e}_1 + E'^2 \mathbf{e}_2 + E'^3 \mathbf{e}_3) = E'^2 \mathbf{e}_3 - E'^3 \mathbf{e}_2 \tag{73}$$

Taking into account (72)-(73) the system of equations (71) is divided off into two independent systems of two equations each and two additional independent equations:

$$\begin{cases} \frac{\partial' E'^2}{\partial' v} = -B'^3, & \begin{cases} \frac{\partial' E'^3}{\partial' v} = B'^2, \\ \frac{\partial' B'^2}{\partial' v} = \frac{\epsilon\mu}{c^2} E'^3; \end{cases} & \frac{\partial' E'^1}{\partial' v} = 0; \quad \frac{\partial' B'^1}{\partial' v} = 0 \end{cases} \quad (74)$$

We differentiate the first equations of systems (74) and will substitute them the secondly:

$$\frac{\partial'^2 E'^2}{\partial' v^2} = \frac{\epsilon\mu}{c^2} E'^2; \quad \frac{\partial'^2 E'^3}{\partial' v^2} = \frac{\epsilon\mu}{c^2} E'^3; \quad \frac{\partial'^2 B'^2}{\partial' v^2} = \frac{\epsilon\mu}{c^2} B'^2; \quad \frac{\partial'^2 B'^3}{\partial' v^2} = \frac{\epsilon\mu}{c^2} B'^3 \quad (75)$$

The general solution of equations (75) is expressed as the arbitrary constants C_1, \dots, C_{10} :

$$E'^1 = C_1; \quad E'^2 = C_2 \cosh \frac{\sqrt{\epsilon\mu v}}{c} + C_3 \sinh \frac{\sqrt{\epsilon\mu v}}{c}; \quad E'^3 = C_4 \cosh \frac{\sqrt{\epsilon\mu v}}{c} + C_5 \sinh \frac{\sqrt{\epsilon\mu v}}{c}; \quad (76)$$

$$B'^1 = C_6; \quad B'^2 = C_7 \cosh \frac{\sqrt{\epsilon\mu v}}{c} + C_8 \sinh \frac{\sqrt{\epsilon\mu v}}{c}; \quad B'^3 = C_9 \cosh \frac{\sqrt{\epsilon\mu v}}{c} + C_{10} \sinh \frac{\sqrt{\epsilon\mu v}}{c}. \quad (77)$$

Since we search for the conversions of electromagnetic field upon transfer from the laboratory frame of reference, then the desired particular solutions of equations (75) must with $v = 0$ describe

electromagnetic field in the laboratory frame of reference, i.e., satisfy equalities (8) and (74), and the, which means, following totality of the equalities:

$$E'^1(0, \mathbf{r}', t) = E^1(\mathbf{r}', t) \quad E'^2(0, \mathbf{r}', t) = E^2(\mathbf{r}', t) \quad E'^3(0, \mathbf{r}', t) = E^3(\mathbf{r}', t); \quad (78)$$

$$B'^1(0, \mathbf{r}', t) = B^1(\mathbf{r}', t); \quad B'^2(0, \mathbf{r}', t) = B^2(\mathbf{r}', t); \quad B'^3(0, \mathbf{r}', t) = B^3(\mathbf{r}', t); \quad (79)$$

$$\frac{\partial' E'^2(0, \mathbf{r}', t)}{\partial' v} = -B^3(\mathbf{r}', t); \quad \frac{\partial' E'^3(0, \mathbf{r}', t)}{\partial' v} = B^2(\mathbf{r}', t); \quad (80)$$

$$\frac{\partial' B'^2(0, \mathbf{r}', t)}{\partial' v} = \frac{\epsilon\mu}{c^2} E^3(\mathbf{r}', t), \quad \frac{\partial' B'^3(0, \mathbf{r}', t)}{\partial' v} = -\frac{\epsilon\mu}{c^2} E^2(\mathbf{r}', t). \quad (81)$$

By substitution (76)-(77) in (78)-(81) let us find the values of constants C_1, \dots, C_{10} , as a result what after the substitution of these constants in (76)-(77) we will obtain the resultant expression in the component

form for the desired conversions of electromagnetic field upon transfer from the laboratory frame of reference to the substantive:

$$E'^1(v, \mathbf{r}', t) = E^1(\mathbf{r}', t), \quad B'^1(v, \mathbf{r}', t) = B^1(\mathbf{r}', t) \quad (82)$$

$$E'^2(v, \mathbf{r}', t) = E^2(\mathbf{r}', t) \cosh \frac{\sqrt{\epsilon\mu v}}{c} - \frac{c}{\sqrt{\epsilon\mu}} B^3(\mathbf{r}', t) \sinh \frac{\sqrt{\epsilon\mu v}}{c}; \quad (83)$$

$$E'^3(v, \mathbf{r}', t) = E^3(\mathbf{r}', t) \cosh \frac{\sqrt{\epsilon\mu v}}{c} + \frac{c}{\sqrt{\epsilon\mu}} B^2(\mathbf{r}', t) \sinh \frac{\sqrt{\epsilon\mu v}}{c} \quad (84)$$

$$B'^2(v, \mathbf{r}', t) = B^2(\mathbf{r}', t) \cosh \frac{\sqrt{\epsilon\mu v}}{c} + \frac{\sqrt{\epsilon\mu}}{c} E^3(\mathbf{r}', t) \sinh \frac{\sqrt{\epsilon\mu v}}{c} \quad (85)$$

$$B'^3(v, \mathbf{r}', t) = B^3(\mathbf{r}', t) \cosh \frac{\sqrt{\varepsilon\mu}v}{c} - \frac{\sqrt{\varepsilon\mu}}{c} \mathbf{E}^2(\mathbf{r}', t) \sinh \frac{\sqrt{\varepsilon\mu}v}{c} \quad (86)$$

In the vector form the same conversions take the following form:

$$\mathbf{E}'(v, \mathbf{r}', t) = \mathbf{E}(\mathbf{r}', t) \cosh \frac{\sqrt{\varepsilon\mu}v}{c} + \frac{c}{\sqrt{\varepsilon\mu}} \mathbf{e}_1 \times \mathbf{B}(\mathbf{r}', t) \sinh \frac{\sqrt{\varepsilon\mu}v}{c} \quad (87)$$

$$\mathbf{B}'(v, \mathbf{r}', t) = \mathbf{B}(\mathbf{r}', t) \cosh \frac{\sqrt{\varepsilon\mu}v}{c} - \frac{\sqrt{\varepsilon\mu}}{c} \mathbf{e}_1 \times \mathbf{E}(\mathbf{r}', t) \sinh \frac{\sqrt{\varepsilon\mu}v}{c}. \quad (88)$$

It is easy to see that the conversions (82)-(88) are known Mende conversions.

V. CONCLUSION

Thus, the Mende conversions obtain a sufficient theoretical substantiation within the framework of the trans-coordinate formulation of electrodynamics, connected with the gipercontinual ideas about the space and the time, and also with the concept not of the invariance of electric charge relative to the speed of the motion of observer. Together with that been in [9] direct experimental confirmation of the concept not of the invariance of electric charge, this is convincing evidence of their larger adequacy of physical reality on the comparison not only with the classical, but also with the relativistic conversions of electromagnetic field, or the convincing evidence of the justification of the transfer of electrodynamics from the traditional formulation of Hertz-Heaviside to the trans-coordinate. The sequential development of transcoordinate electrodynamics is capable of not only deriving on the new qualitative level of idea about the space and the time, but also of opening the fundamentally new horizons of the development engineering and technologies due to the discovery and the mastery of new physical phenomena and effects.

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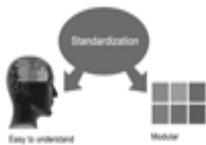
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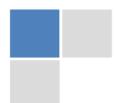
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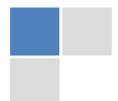
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- Use standard style in this and in every other part of the paper - avoid familiar lists, and use full sentences.

What to keep away from

- Resources and methods are not a set of information.
- Skip all descriptive information and surroundings - save it for the argument.
- Leave out information that is immaterial to a third party.

Results:

The principle of a results segment is to present and demonstrate your conclusion. Create this part a entirely objective details of the outcome, and save all understanding for the discussion.

The page length of this segment is set by the sum and types of data to be reported. Carry on to be to the point, by means of statistics and tables, if suitable, to present consequences most efficiently. You must obviously differentiate material that would usually be incorporated in a study editorial from any unprocessed data or additional appendix matter that would not be available. In fact, such matter should not be submitted at all except requested by the instructor.



Content

- Sum up your conclusion in text and demonstrate them, if suitable, with figures and tables.
- In manuscript, explain each of your consequences, point the reader to remarks that are most appropriate.
- Present a background, such as by describing the question that was addressed by creation an exacting study.
- Explain results of control experiments and comprise remarks that are not accessible in a prescribed figure or table, if appropriate.
- Examine your data, then prepare the analyzed (transformed) data in the form of a figure (graph), table, or in manuscript form.

What to stay away from

- Do not discuss or infer your outcome, report surroundings information, or try to explain anything.
- Not at all, take in raw data or intermediate calculations in a research manuscript.
- Do not present the similar data more than once.
- Manuscript should complement any figures or tables, not duplicate the identical information.
- Never confuse figures with tables - there is a difference.

Approach

- As forever, use past tense when you submit to your results, and put the whole thing in a reasonable order.
- Put figures and tables, appropriately numbered, in order at the end of the report
- If you desire, you may place your figures and tables properly within the text of your results part.

Figures and tables

- If you put figures and tables at the end of the details, make certain that they are visibly distinguished from any attach appendix materials, such as raw facts
- Despite of position, each figure must be numbered one after the other and complete with subtitle
- In spite of position, each table must be titled, numbered one after the other and complete with heading
- All figure and table must be adequately complete that it could situate on its own, divide from text

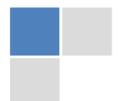
Discussion:

The Discussion is expected the trickiest segment to write and describe. A lot of papers submitted for journal are discarded based on problems with the Discussion. There is no head of state for how long a argument should be. Position your understanding of the outcome visibly to lead the reviewer through your conclusions, and then finish the paper with a summing up of the implication of the study. The purpose here is to offer an understanding of your results and hold up for all of your conclusions, using facts from your research and generally accepted information, if suitable. The implication of result should be visibly described. Infer your data in the conversation in suitable depth. This means that when you clarify an observable fact you must explain mechanisms that may account for the observation. If your results vary from your prospect, make clear why that may have happened. If your results agree, then explain the theory that the proof supported. It is never suitable to just state that the data approved with prospect, and let it drop at that.

- Make a decision if each premise is supported, discarded, or if you cannot make a conclusion with assurance. Do not just dismiss a study or part of a study as "uncertain."
- Research papers are not acknowledged if the work is imperfect. Draw what conclusions you can based upon the results that you have, and take care of the study as a finished work
- You may propose future guidelines, such as how the experiment might be personalized to accomplish a new idea.
- Give details all of your remarks as much as possible, focus on mechanisms.
- Make a decision if the tentative design sufficiently addressed the theory, and whether or not it was correctly restricted.
- Try to present substitute explanations if sensible alternatives be present.
- One research will not counter an overall question, so maintain the large picture in mind, where do you go next? The best studies unlock new avenues of study. What questions remain?
- Recommendations for detailed papers will offer supplementary suggestions.

Approach:

- When you refer to information, differentiate data generated by your own studies from available information
- Submit to work done by specific persons (including you) in past tense.
- Submit to generally acknowledged facts and main beliefs in present tense.



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<i>Methods and Procedures</i>	Clear and to the point with well arranged paragraph, precision and accuracy of facts and figures, well organized subheads	Difficult to comprehend with embarrassed text, too much explanation but completed	Incorrect and unorganized structure with hazy meaning
<i>Result</i>	Well organized, Clear and specific, Correct units with precision, correct data, well structuring of paragraph, no grammar and spelling mistake	Complete and embarrassed text, difficult to comprehend	Irregular format with wrong facts and figures
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<i>References</i>	Complete and correct format, well organized	Beside the point, Incomplete	Wrong format and structuring



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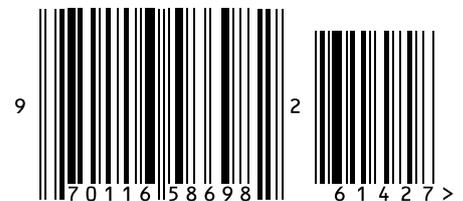


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